250 MHz, General Purpose Voltage Feedback Op Amps

AD8047/AD8048

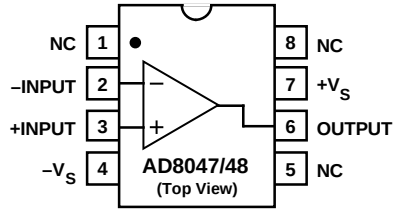
FEATURES

Wide Bandwidth	**AD8047, G = +1**	**AD8048, G = +2**
Small Signal	**250 MHz**	**260 MHz**
Large Signal (2 V p-p)	**130 MHz**	**160 MHz**

5.8 mA Typical Supply Current
Low Distortion, (SFDR) Low Noise
–66 dBc typ @ 5 MHz
–54 dBc typ @ 20 MHz
5.2 nV/$\sqrt{Hz}$ (AD8047), 3.8 nV/$\sqrt{Hz}$ (AD8048) Noise
Drives 50 pF Capacitive Load
High Speed
Slew Rate 750 V/μs (AD8047), 1000 V/μs (AD8048)
Settling 30 ns to 0.01%, 2 V Step
±3 V to ±6 V Supply Operation

APPLICATIONS
Low Power ADC Input Driver
Differential Amplifiers
IF/RF Amplifiers
Pulse Amplifiers
Professional Video
DAC Current to Voltage Conversion
Baseband and Video Communications
Pin Diode Receivers
Active Filters/Integrators

FUNCTIONAL BLOCK DIAGRAM
8-Pin Plastic Mini-DIP (N), Cerdip (Q) and SO (R) Packages



NC = NO CONNECT

PRODUCT DESCRIPTION

The AD8047 and AD8048 are very high speed and wide bandwidth amplifiers. The AD8047 is unity gain stable. The AD8048 is stable at gains of two or greater. The AD8047 and AD8048, which utilize a voltage feedback architecture, meet the requirements of many applications that previously depended on current feedback amplifiers.

A proprietary circuit has produced an amplifier that combines many of the best characteristics of both current feedback and voltage feedback amplifiers. For the power (6.6 mA max) the AD8047 and AD8048 exhibit fast and accurate pulse response (30 ns to 0.01%) as well as extremely wide small signal and large signal bandwidth and low distortion. The AD8047 achieves –54 dBc distortion at 20 MHz and 250 MHz small signal and 130 MHz large signal bandwidths.

The AD8047 and AD8048's low distortion and cap load drive make the AD8047/AD8048 ideal for buffering high speed ADCs. They are suitable for 12 bit/10 MSPS or 8 bit/60 MSPS ADCs. Additionally, the balanced high impedance inputs of the voltage feedback architecture allow maximum flexibility when designing active filters.

The AD8047 and AD8048 are offered in industrial (–40°C to +85°C) temperature ranges and are available in 8-pin plastic DIP and SOIC packages.

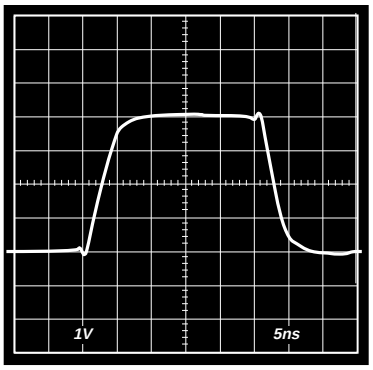


Figure 1. AD8047 Large Signal Transient Response, V_O = 4 V p-p, G = +1

REV. 0

One Technology Way, P.O. Box 9106, Norwood. MA 02062-9106, U.S.A.
Tel: 617/329-4700 **Fax: 617/326-8703**

AD8047/AD8048–SPECIFICATIONS

ELECTRICAL CHARACTERISTICS ($\pm V_S = \pm 5$ V; $R_{LOAD} = 100\ \Omega$; $A_V = 1$ (AD8047); $A_V = 2$ (AD8048), unless otherwise noted)

Parameter	Conditions	AD8047A Min	AD8047A Typ	AD8047A Max	AD8048A Min	AD8048A Typ	AD8048A Max	Units
DYNAMIC PERFORMANCE								
Bandwidth (–3 dB)								
Small Signal	$V_{OUT} \le 0.4$ V p-p	170	250		180	260		MHz
Large Signal[1]	V_{OUT} = 2 V p-p	100	130		135	160		MHz
Bandwidth for 0.1 dB Flatness	V_{OUT} = 300 mV p-p							
	8047, $R_F = 0\ \Omega$; 8048, $R_F = 200\ \Omega$		35			50		MHz
Slew Rate, Average +/–	V_{OUT} = 4 V Step	475	750		740	1000		V/µs
Rise/Fall Time	V_{OUT} = 0.5 V Step		1.1			1.2		ns
	V_{OUT} = 4 V Step		4.3			3.2		ns
Settling Time								
To 0.1%	V_{OUT} = 2 V Step		13			13		ns
To 0.01%	V_{OUT} = 2 V Step		30			30		ns
HARMONIC/NOISE PERFORMANCE								
2nd Harmonic Distortion	2 V p-p; 20 MHz		–54			–48		dBc
	$R_L = 1\ k\Omega$		–64			–60		dBc
3rd Harmonic Distortion	2 V p-p; 20 MHz		–60			–56		dBc
	$R_L = 1\ k\Omega$		–61			–65		dBc
Input Voltage Noise	f = 100 kHz		5.2			3.8		nV/√Hz
Input Current Noise	f = 100 kHz		1.0			1.0		pA/√Hz
Average Equivalent Integrated								
Input Noise Voltage	0.1 MHz to 10 MHz		16			11		µV rms
Differential Gain Error (3.58 MHz)	$R_L = 150\ \Omega$, G = +2		0.02			0.01		%
Differential Phase Error (3.58 MHz)	$R_L = 150\ \Omega$, G = +2		0.03			0.02		Degree
DC PERFORMANCE[2], $R_L = 150\ \Omega$								
Input Offset Voltage[3]			1	3		1	3	mV
	T_{MIN}–T_{MAX}			4			4	mV
Offset Voltage Drift			±5			±5		µV/°C
Input Bias Current			1	3.5		1	3.5	µA
	T_{MIN}–T_{MAX}			6.5			6.5	µA
Input Offset Current			0.5	2		0.5	2	µA
	T_{MIN}–T_{MAX}			3			3	µA
Common-Mode Rejection Ratio	$V_{CM} = \pm 2.5$ V	74	80		74	80		dB
Open-Loop Gain	$V_{OUT} = \pm 2.5$ V	58	62		65	68		dB
	T_{MIN}–T_{MAX}	54			56			dB
INPUT CHARACTERISTICS								
Input Resistance			500			500		kΩ
Input Capacitance			1.5			1.5		pF
Input Common-Mode Voltage Range			±3.4			±3.4		V
OUTPUT CHARACTERISTICS								
Output Voltage Range, $R_L = 150\ \Omega$		±2.8	±3.0		±2.8	±3.0		V
Output Current			50			50		mA
Output Resistance			0.2			0.2		Ω
Short Circuit Current			130			130		mA
POWER SUPPLY								
Operating Range		±3.0	±5.0	±6.0	±3.0	±5.0	±6.0	V
Quiescent Current			5.8	6.6		5.9	6.6	mA
	T_{MIN}–T_{MAX}			7.5			7.5	mA
Power Supply Rejection Ratio		72	78		72	78		dB

NOTES

[1]See Max Ratings and Theory of Operation sections of data sheet.

[2]Measured at $A_V = 50$.

[3]Measured with respect to the inverting input.

Specifications subject to change without notice.

ABSOLUTE MAXIMUM RATINGS[1]

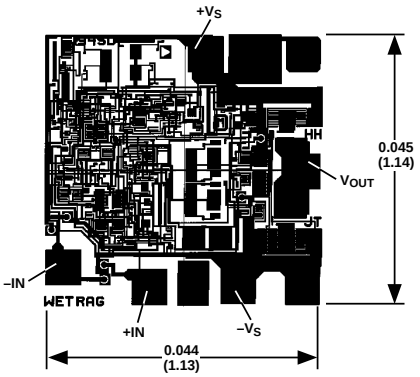
Supply Voltage . . . . . 12.6 V
Voltage Swing × Bandwidth Product (AD8047) . . . 180 V – MHz
(AD8048) . . . 250 V– MHz
Internal Power Dissipation[2]
Plastic Package (N) . . . . . 1.3 Watts
Small Outline Package (R) . . . . . 0.9 Watts
Input Voltage (Common Mode) . . . . . $\pm V_S$
Differential Input Voltage . . . . . ±1.2 V
Output Short Circuit Duration
. . . . . Observe Power Derating Curves
Storage Temperature Range (N, R) . . . . . –65°C to +125°C
Operating Temperature Range (A Grade) . . . –40°C to +85°C
Lead Temperature Range (Soldering 10 sec) . . . . . +300°C

NOTES
[1]Stresses above those listed under "Absolute Maximum Ratings" may cause permanent damage to the device. This is a stress rating only, and functional operation of the device at these or any other conditions above those indicated in the operational section of this specification is not implied. Exposure to absolute maximum rating conditions for extended periods may affect device reliability.
[2]Specification is for device in free air:
8-Pin Plastic DIP Package: θ_{JA} = 90°C/Watt
8-Pin SOIC Package: θ_{JA} = 140°C/Watt

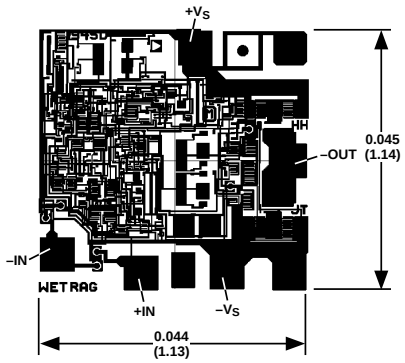
METALIZATION PHOTOS

Dimensions shown in inches and (mm).
Connect Substrate to $-V_S$.

AD8047



AD8048



MAXIMUM POWER DISSIPATION

The maximum power that can be safely dissipated by these devices is limited by the associated rise in junction temperature. The maximum safe junction temperature for plastic encapsulated devices is determined by the glass transition temperature of the plastic, approximately +150°C. Exceeding this limit temporarily may cause a shift in parametric performance due to a change in the stresses exerted on the die by the package. Exceeding a junction temperature of +175°C for an extended period can result in device failure.

While the AD8047 and AD8048 are internally short circuit protected, this may not be sufficient to guarantee that the maximum junction temperature (+150°C) is not exceeded under all conditions. To ensure proper operation, it is necessary to observe the maximum power derating curves.

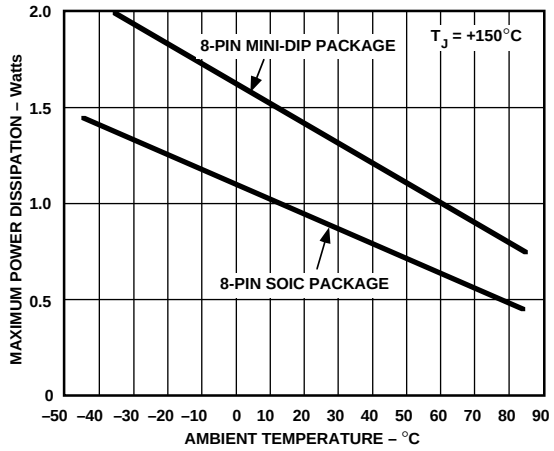


Figure 2. Plot of Maximum Power Dissipation vs. Temperature

ORDERING GUIDE

Model	Temperature Range	Package Description	Package Option*
AD8047AN	–40°C to +85°C	Plastic DIP	N-8
AD8047AR	–40°C to +85°C	SOIC	R-8
AD8047-EB		Evaluation Board	
AD8048AN	–40°C to +85°C	Plastic DIP	N-8
AD8048AR	–40°C to +85°C	SOIC	R-8
AD8048-EB		Evaluation Board	

*N = Plastic DIP; R= SOIC (Small Outline Integrated Circuit)

CAUTION

ESD (electrostatic discharge) sensitive device. Electrostatic charges as high as 4000 V readily accumulate on the human body and test equipment and can discharge without detection. Although these devices feature proprietary ESD protection circuitry, permanent damage may occur on devices subjected to high energy electrostatic discharges. Therefore, proper ESD precautions are recommended to avoid performance degradation or loss of functionality.

AD8047–Typical Characteristics

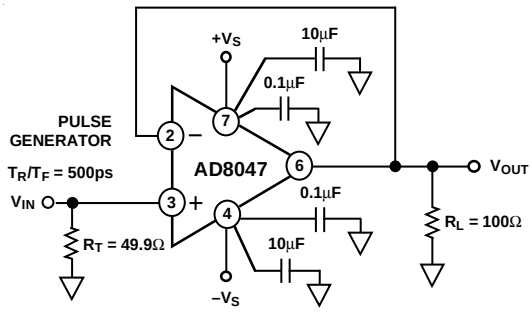


Figure 3. Noninverting Configuration, G = +1

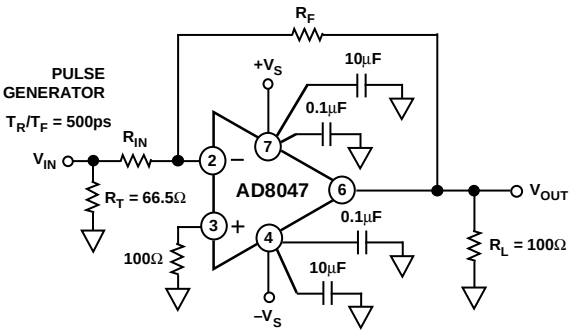


Figure 6. Inverting Configuration, G = –1

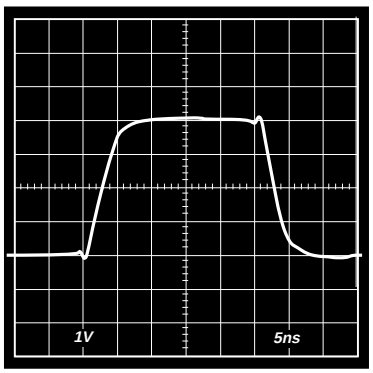


Figure 4. Large Signal Transient Response; V_O = 4 V p-p, G = +1

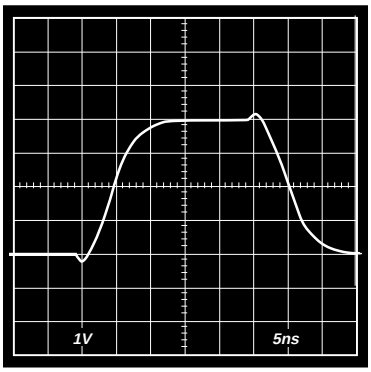


Figure 7. Large Signal Transient Response; V_O = 4 V p-p, G = –1, $R_F = R_{IN}$ = 200 Ω

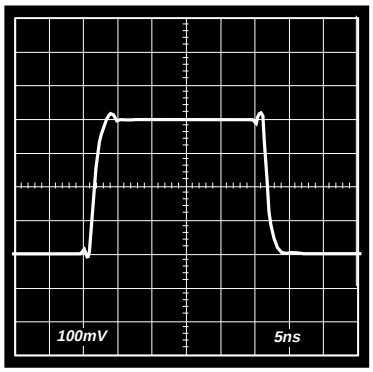


Figure 5. Small Signal Transient Response; V_O = 400 mV p-p, G = +1

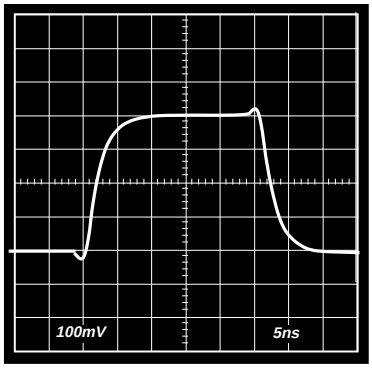


Figure 8. Small Signal Transient Response; V_O = 400 mV p-p, G = –1, $R_F = R_{IN}$ = 200 Ω

AD8048–Typical Characteristics

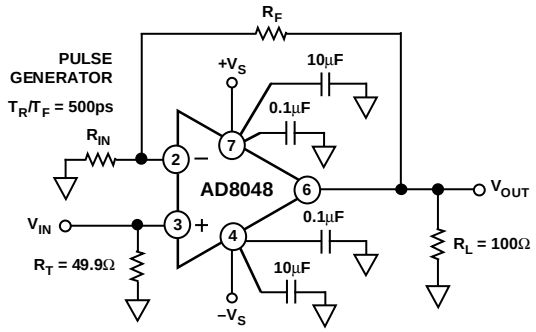


Figure 9. Noninverting Configuration, G = +2

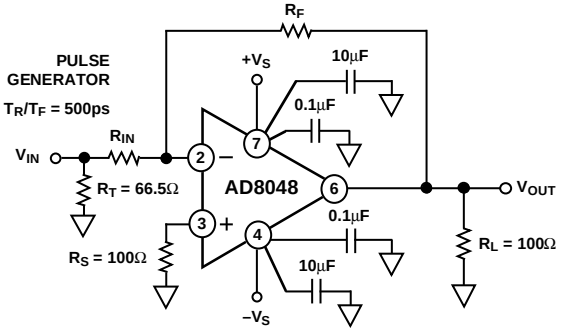


Figure 12. Inverting Configuration, G= –1

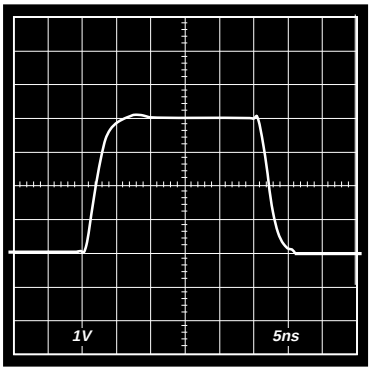


Figure 10. Large Signal Transient Response; V_O = 4 V p-p, G = +2, $R_F = R_{IN}$ = 200 Ω

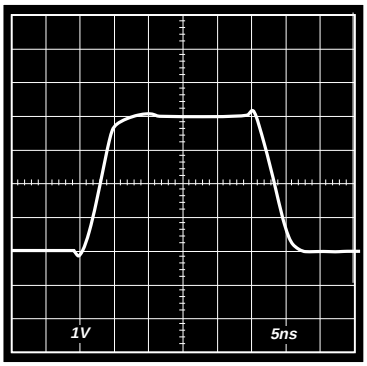


Figure 13. Large Signal Transient Response; V_O = 4 V p-p, G = –1, $R_F = R_{IN}$ = 200 Ω

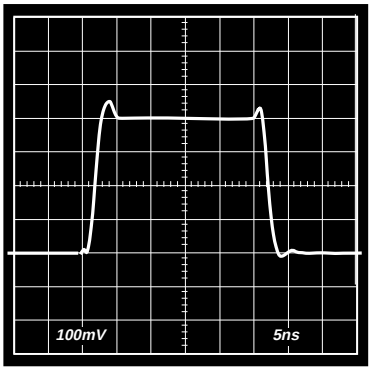


Figure 11. Small Signal Transient Response; V_O = 400 mV p-p, G = +2, $R_F = R_{IN}$ = 200 Ω

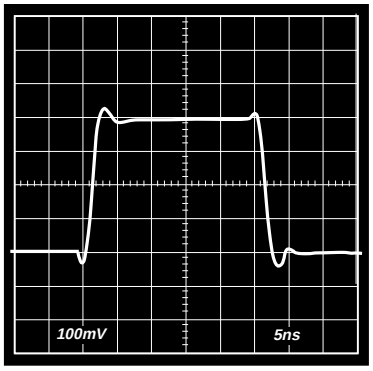


Figure 14. Small Signal Transient Response; V_O = 400 mV p-p, G = –1, $R_F = R_{IN}$ = 200 Ω

AD8047–Typical Characteristics

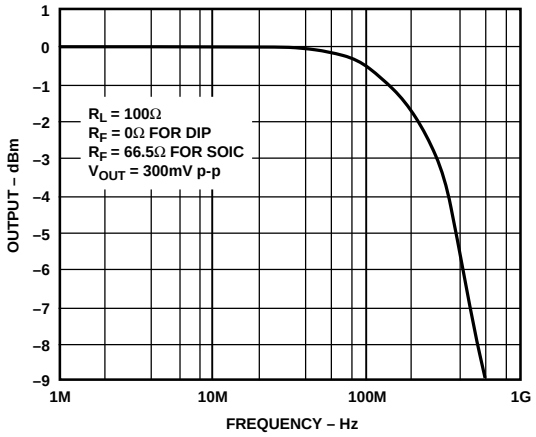


Figure 15. AD8047 Small Signal Frequency Response G = +1

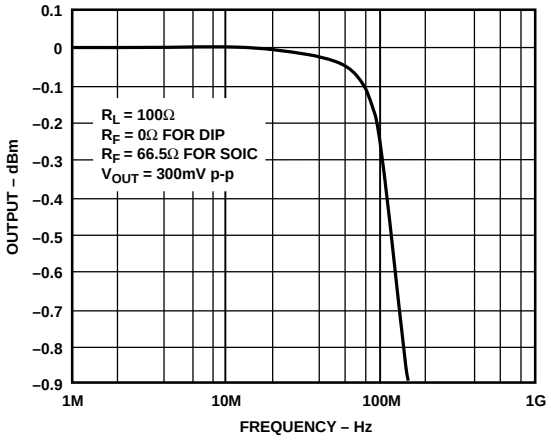


Figure 16. AD8047 0.1 dB Flatness, G = +1

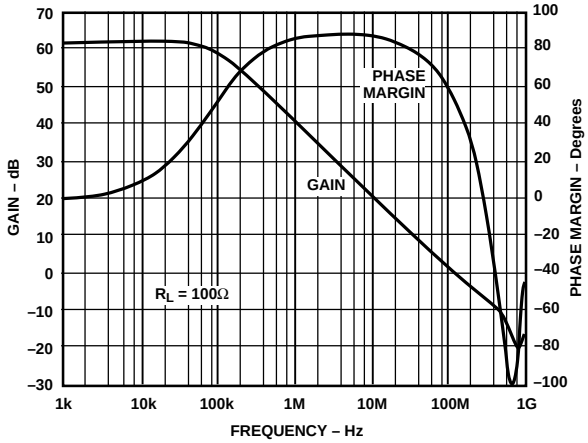


Figure 17. AD8047 Open-Loop Gain and Phase Margin vs. Frequency

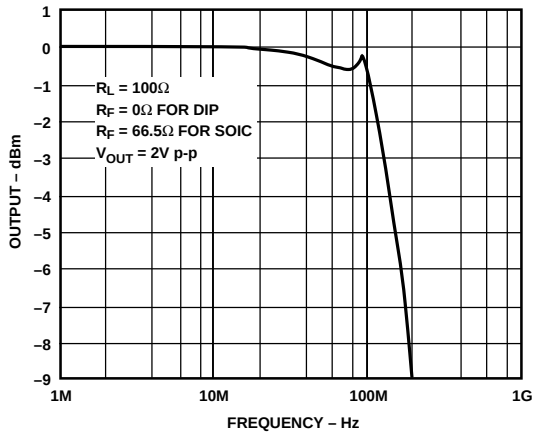


Figure 18. AD8047 Large Signal Frequency Response, G = +1

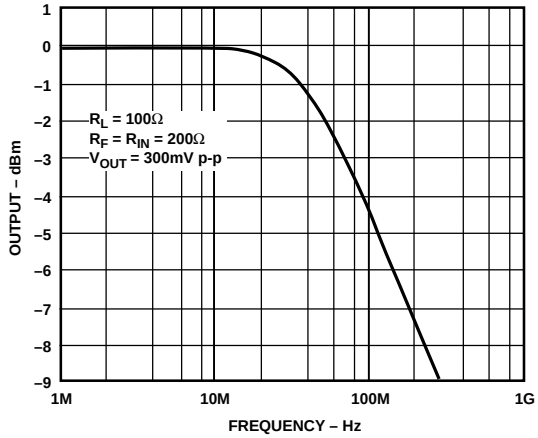


Figure 19. AD8047 Small Signal Frequency Response, G = –1

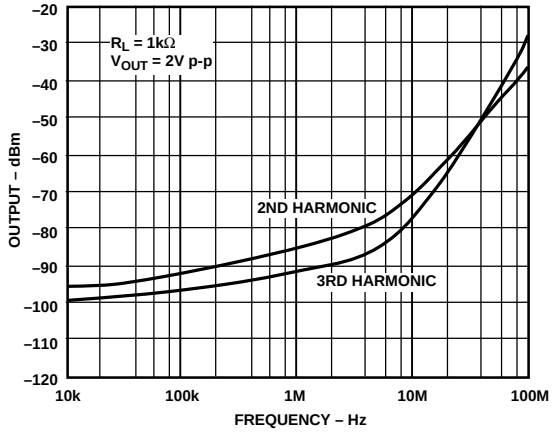


Figure 20. AD8047 Harmonic Distortion vs. Frequency, G = +1

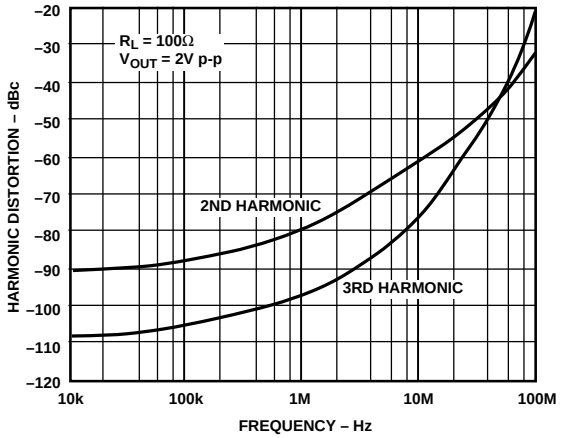


Figure 21. AD8047 Harmonic Distortion vs. Frequency, G = +1

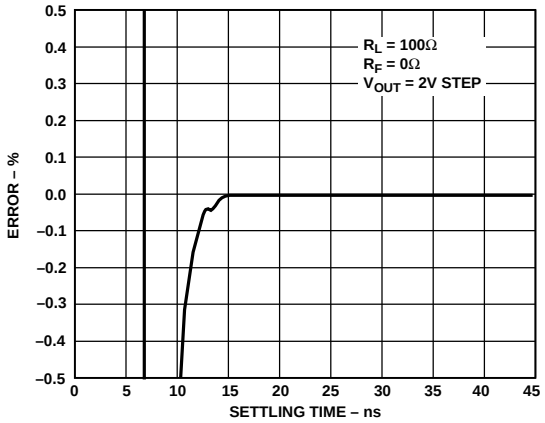


Figure 24. AD8047 Short-Term Settling Time, G = +1

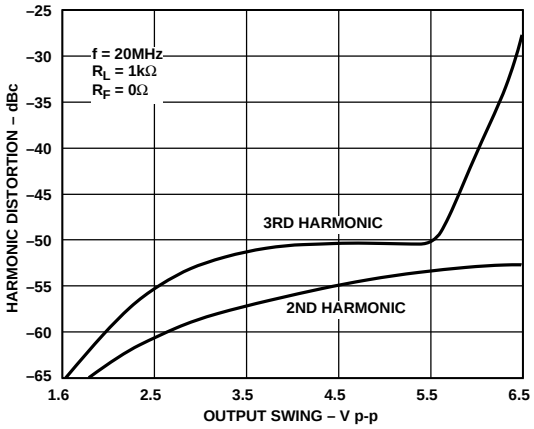


Figure 22. AD8047 Harmonic Distortion vs. Output Swing, G = +1

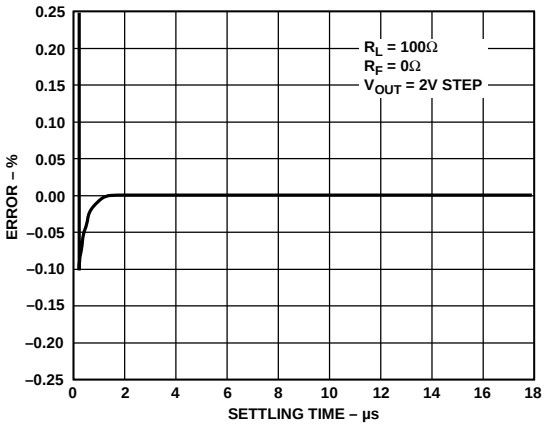


Figure 25. AD8047 Long-Term Settling Time, G = +1

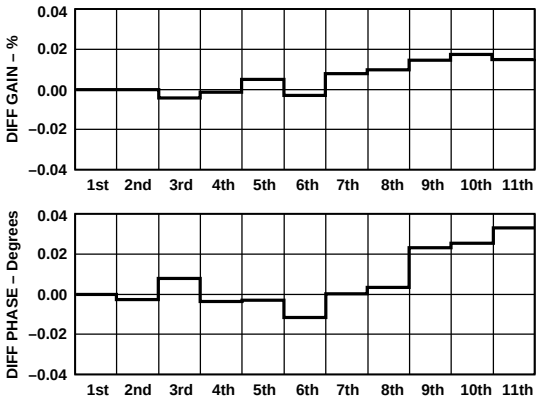


Figure 23. AD8047 Differential Gain and Phase Error, G = +2, R_L = 150 Ω, R_F = 200 Ω, R_{IN} = 200 Ω

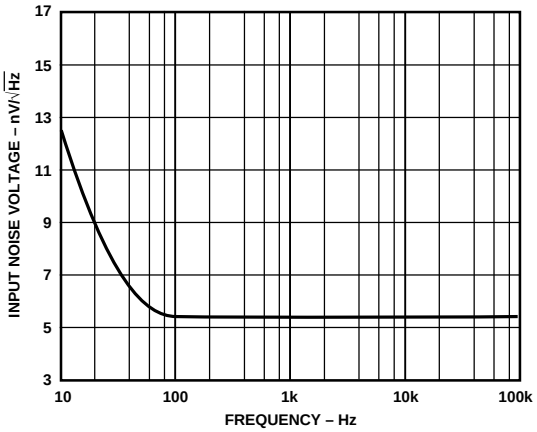


Figure 26. AD8047 Noise vs. Frequency

AD8048–Typical Characteristics

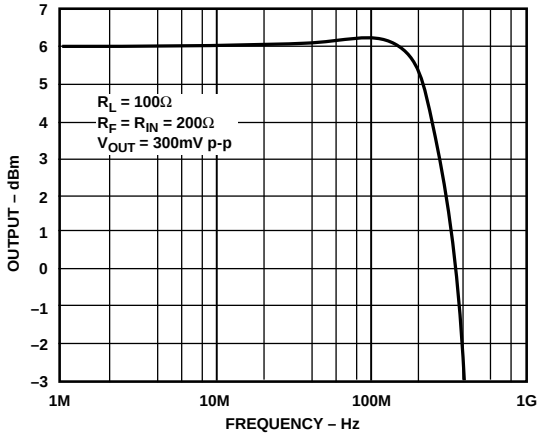


Figure 27. AD8048 Small Signal Frequency Response, G = +2

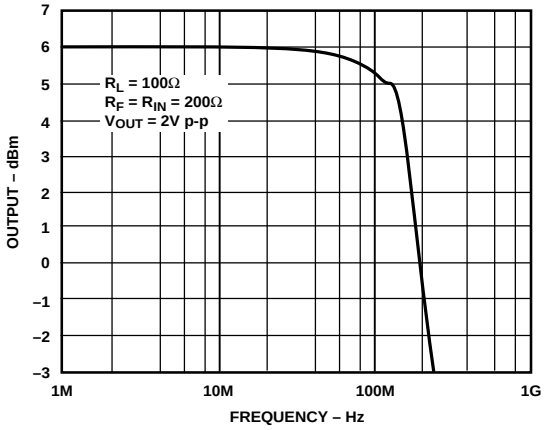


Figure 30. AD8048 Large Signal Frequency Response, G = +2

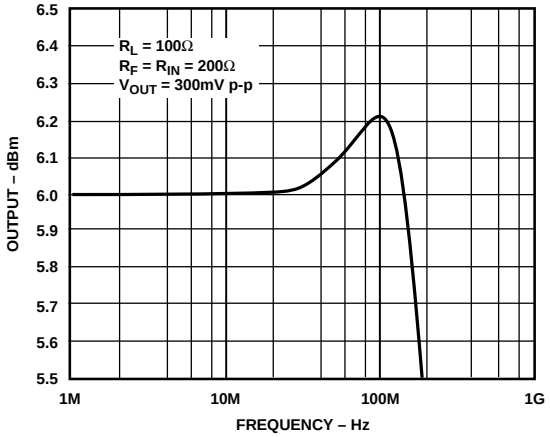


Figure 28. AD8048 0.1 dB Flatness, G = +2

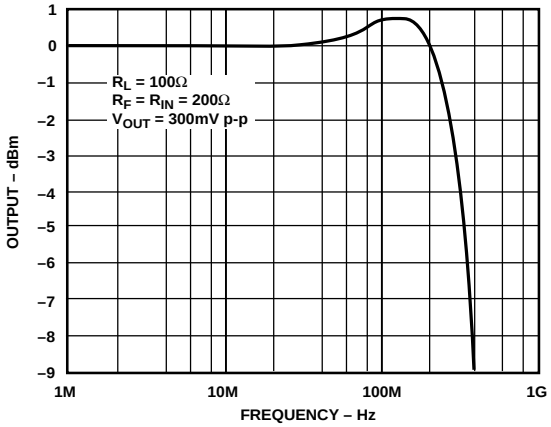


Figure 31. AD8048 Small Signal Frequency Response, G = –1

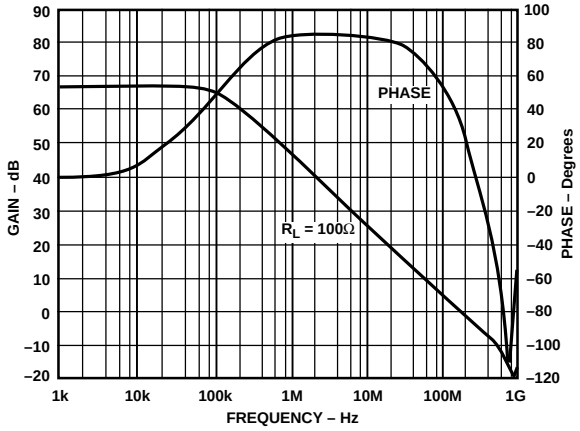


Figure 29. AD8048 Open-Loop Gain and Phase Margin vs. Frequency

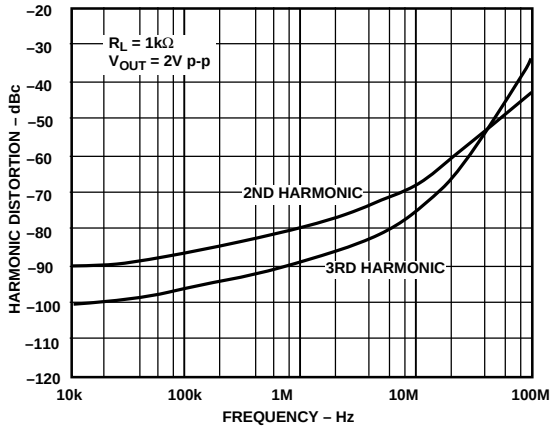


Figure 32. AD8048 Harmonic Distortion vs. Frequency, G = +2

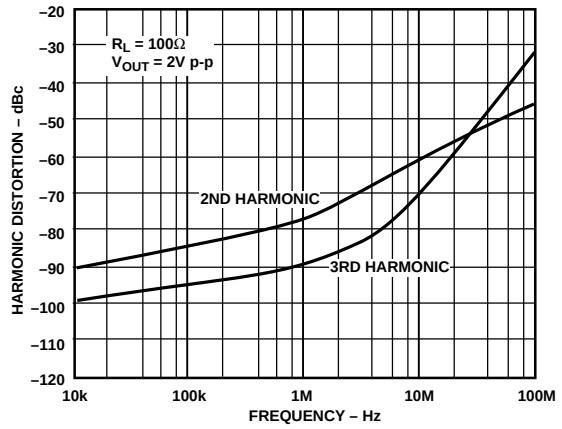


Figure 33. AD8048 Harmonic Distortion vs. Frequency, G = +2

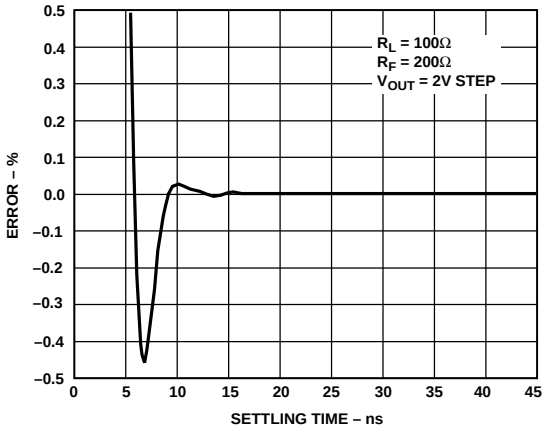


Figure 36. AD8048 Short-Term Settling Time, G = +2

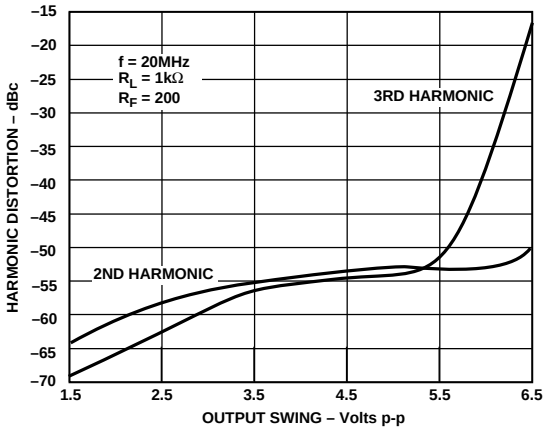


Figure 34. AD8048 Harmonic Distortion vs. Output Swing, G = +2

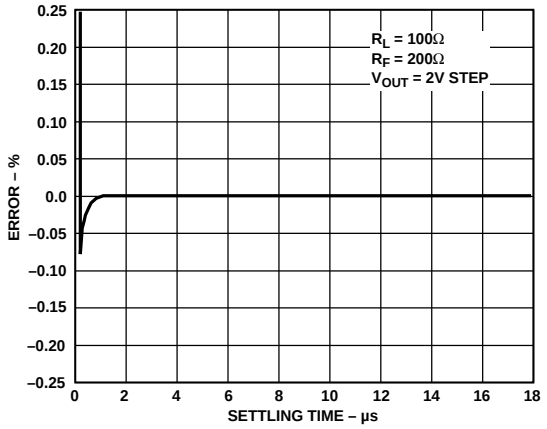


Figure 37. AD8048 Long-Term Settling Time 2 V Step, G = +2

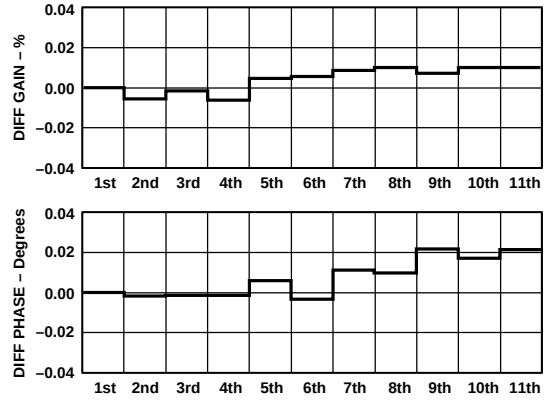


Figure 35. AD8048 Differential Gain and Phase Error, G = +2, R_L = 150 Ω, R_F = 200 Ω, R_{IN} = 200 Ω

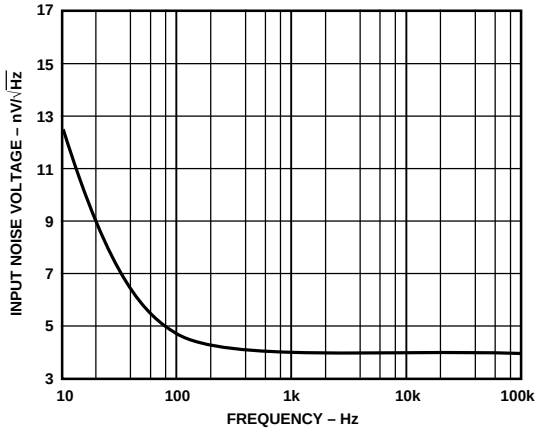


Figure 38. AD8048 Noise vs. Frequency

AD8047/AD8048–Typical Characteristics

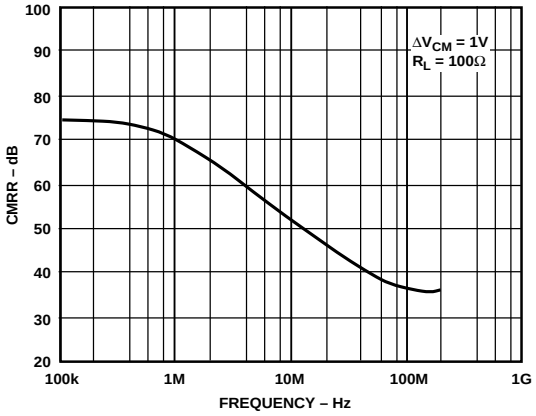


Figure 39. AD8047 CMRR vs. Frequency

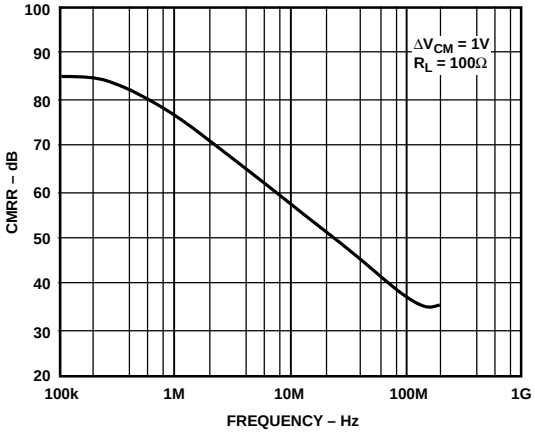


Figure 42. AD8048 CMRR vs. Frequency

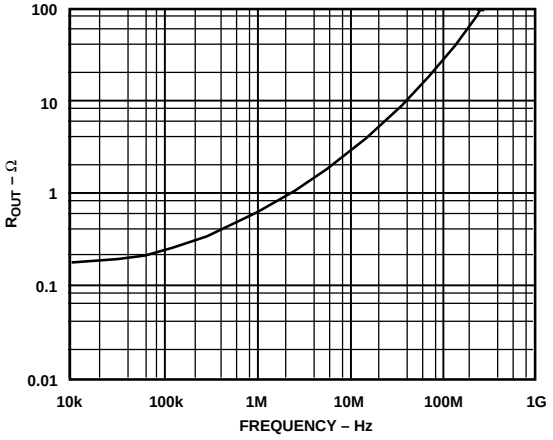


Figure 40. AD8047 Output Resistance vs. Frequency, G = +1

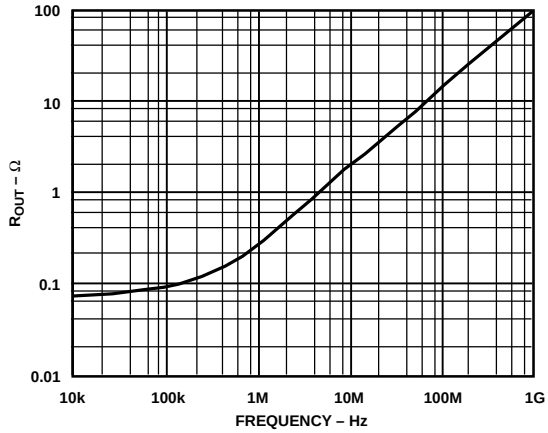


Figure 43. AD8048 Output Resistance vs. Frequency, G = +2

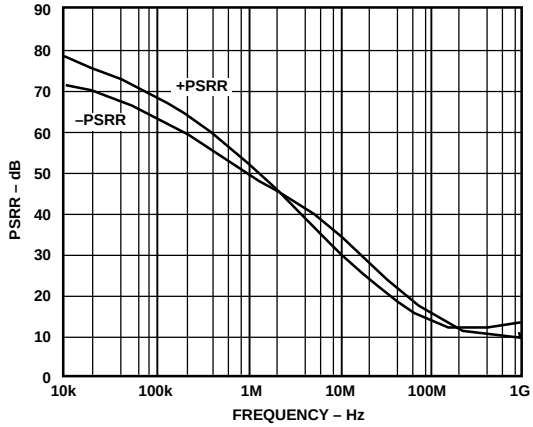


Figure 41. AD8047 PSRR vs. Frequency

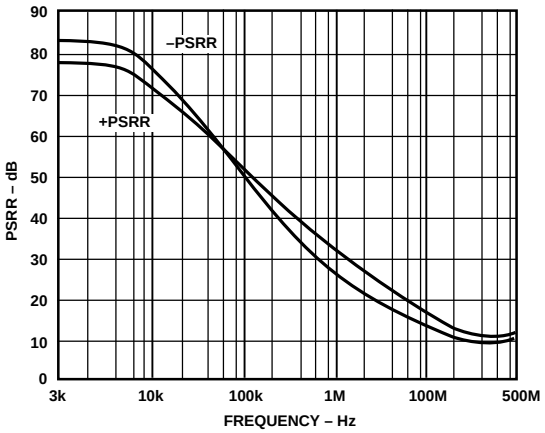


Figure 44. AD8048 PSRR vs. Frequency, G = +2

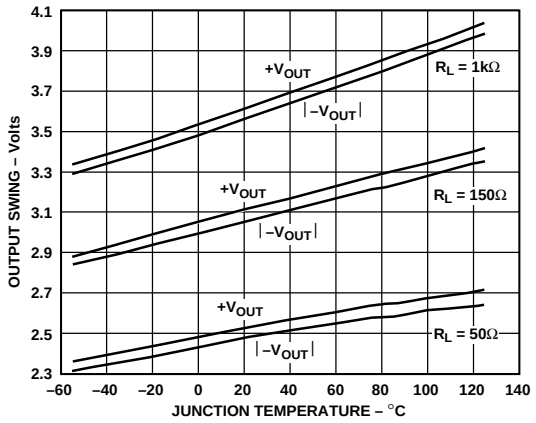


Figure 45. AD8047/AD8048 Output Swing vs. Temperature

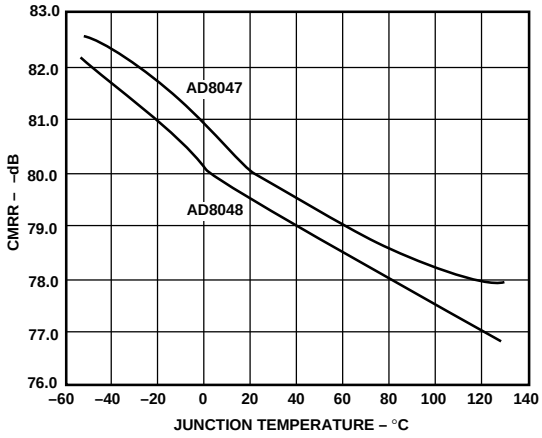


Figure 48. AD8047/AD8048 CMRR vs. Temperature

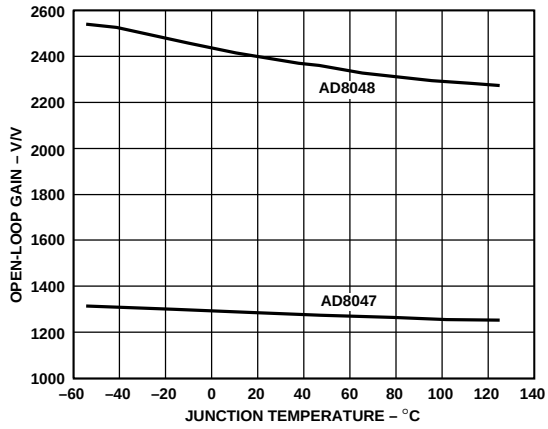


Figure 46. AD8047/AD8048 Open-Loop Gain vs. Temperature

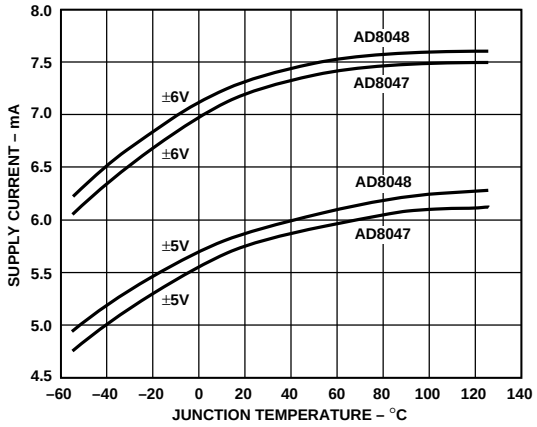


Figure 49. AD8047/AD8048 Supply Current vs. Temperature

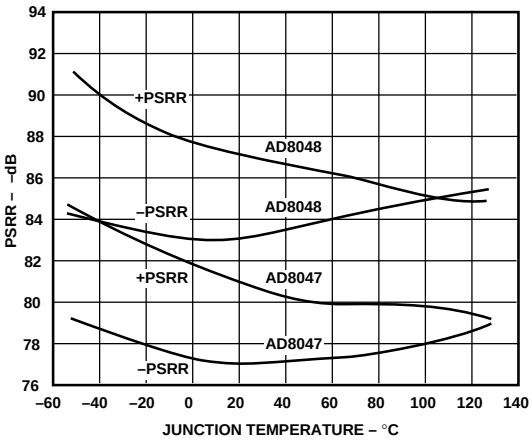


Figure 47. AD8047/AD8048 PSRR vs. Temperature

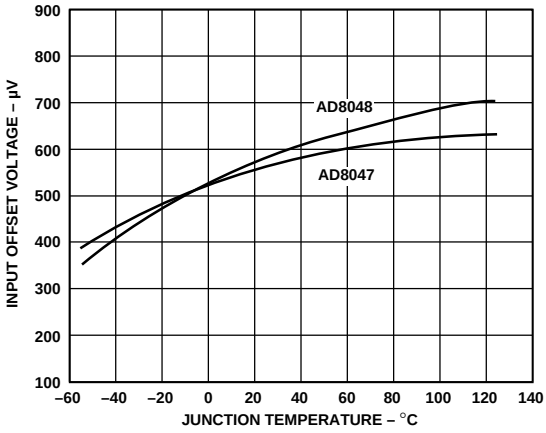


Figure 50. AD8047/AD8048 Input Offset Voltage vs. Temperature

THEORY OF OPERATION

General

The AD8047 and AD8048 are wide bandwidth, voltage feedback amplifiers. Since their open-loop frequency response follows the conventional 6 dB/octave roll-off, their gain bandwidth product is basically constant. Increasing their closed-loop gain results in a corresponding decrease in small signal bandwidth. This can be observed by noting the bandwidth specification between the AD8047 (gain of 1) and AD8048 (gain of 2).

Feedback Resistor Choice

The value of the feedback resistor is critical for optimum performance on the AD8047 and AD8048. For maximum flatness at a gain of 2, R_F and R_G should be set to 200 Ω for the AD8048. When the AD8047 is configured as a unity gain follower, R_F should be set to 0 Ω (no feedback resistor should be used) for the plastic DIP and 66.5 Ω for the SOIC.

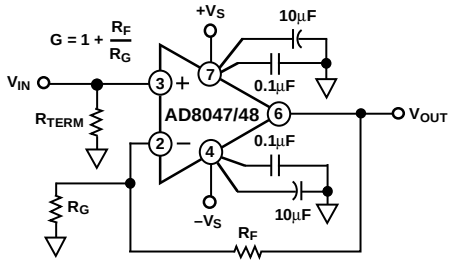


Figure 51. Noninverting Operation

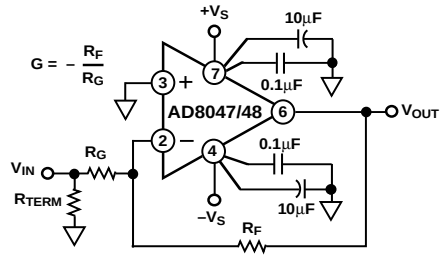


Figure 52. Inverting Operation

When the AD8047 is used in the transimpedance (I to V) mode, such as in photodiode detection, the value of R_F and diode capacitance (C_I) are usually known. Generally, the value of R_F selected will be in the kΩ range, and a shunt capacitor (C_F) across R_F will be required to maintain good amplifier stability. The value of C_F required to maintain optimal flatness (<1 dB Peaking) and settling time can be estimated as:

$$C_F \cong \left[(2\ \omega_O C_I R_F - 1)/\omega_O{}^2\ R_F{}^2\right]^{1/2}$$

where ω_O is equal to the unity gain bandwidth product of the amplifier in rad/sec, and C_I is the equivalent total input capacitance at the inverting input. Typically $\omega_O = 800 \times 10^6$ rad/sec (see Open-Loop Frequency Response curve, Figure 17).

As an example, choosing R_F = 10 kΩ and C_I = 5 pF, requires C_F to be 1.1 pF (Note: C_I includes both source and parasitic circuit capacitance). The bandwidth of the amplifier can be estimated using the C_F calculated as:

$$f_{3\,dB} \cong \frac{1.6}{2\pi R_F C_F}$$

For general voltage gain applications, the amplifier bandwidth can be closely estimated as:

$$f_{3\,dB} \cong \frac{\omega_O}{2\pi\left[1+\left(\frac{R_F}{R_G}\right)\right]}$$

This estimation loses accuracy for gains of +2/–1 or lower due to the amplifier's damping factor. For these "low gain" cases, the bandwidth will actually extend beyond the calculated value (see Closed-Loop BW plots, Figures 15 and 26).

As a rule of thumb, capacitor C_F will not be required if:

$$(R_F \| R_G) \times C_I \le \frac{NG}{4\ \omega_O}$$

where *NG* is the Noise Gain (1 + R_F/R_G) of the circuit. For most voltage gain applications, this should be the case.

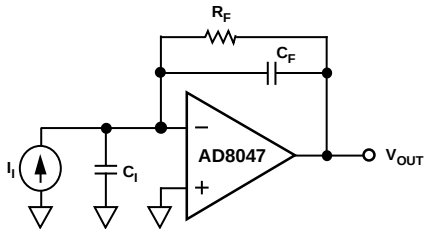


Figure 53. Transimpedance Configuration

Pulse Response

Unlike a traditional voltage feedback amplifier, where the slew speed is dictated by its front end dc quiescent current and gain bandwidth product, the AD8047 and AD8048 provide "on demand" current that increases proportionally to the input "step" signal amplitude. This results in slew rates (1000 V/µs) comparable to wideband current feedback designs. This, combined with relatively low input noise current (1.0 pA/√Hz), gives the AD8047 and AD8048 the best attributes of both voltage and current feedback amplifiers.

Large Signal Performance

The outstanding large signal operation of the AD8047 and AD8048 is due to a unique, proprietary design architecture. In order to maintain this level of performance, the maximum 180 V-MHz product must be observed, (e.g., @ 100 MHz, $V_O \le 1.8$ V p-p) on the AD8047 and 250 V-MHz product on the AD8048.

Power Supply Bypassing

Adequate power supply bypassing can be critical when optimizing the performance of a high frequency circuit. Inductance in the power supply leads can form resonant circuits that produce peaking in the amplifier's response. In addition, if large current transients must be delivered to the load, then bypass capacitors (typically greater than 1 µF) will be required to provide the best settling time and lowest distortion. A parallel combination of at least 4.7 µF, and between 0.1 µF and 0.01 µF, is recommended. Some brands of electrolytic capacitors will require a small series damping resistor ≈4.7 Ω for optimum results.

Driving Capacitive Loads

The AD8047/AD8048 have excellent cap load drive capability for high speed op amps as shown in Figures 55 and 57. However, when driving cap loads greater than 25 pF, the best frequency response is obtained by the addition of a small series resistance. It is worth noting that the frequency response of the

circuit when driving large capacitive loads will be dominated by the passive roll-off of R_{SERIES} and C_L.

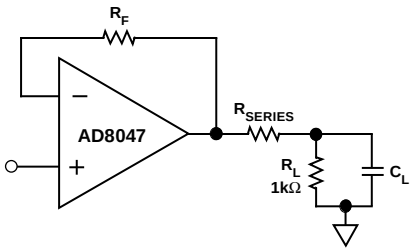


Figure 54. Driving Capacitive Loads

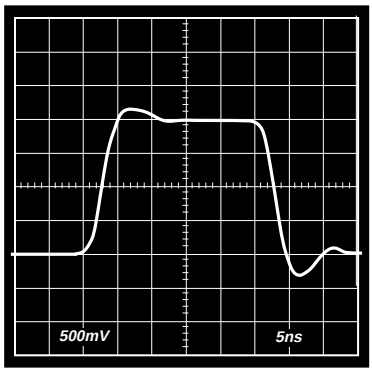


Figure 55. AD8047 Large Signal Transient Response; V_O = 2 V p-p, G = +1, R_F = 0 Ω, R_{SERIES} = 0 Ω, C_L = 27 pF

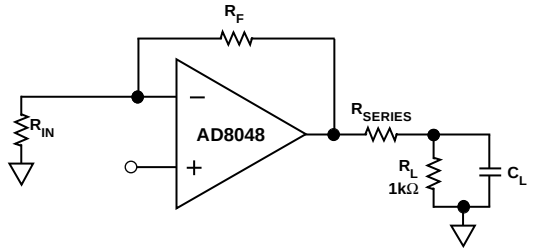


Figure 56. Driving Capacitive Loads

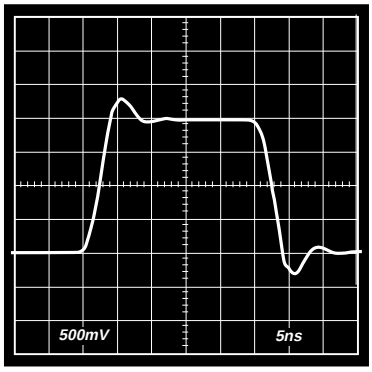


Figure 57. AD8048 Large Signal Transient Response; V_O = 2 V p-p, G = +2, R_F = R_{IN} = 200 Ω, R_{SERIES} = 0 Ω, C_L = 27 pF

APPLICATIONS

The AD8047 and AD8048 are voltage feedback amplifiers well suited for such applications as photodetectors, active filters, and log amplifiers. The devices' wide bandwidth (260 MHz), phase margin (65°), low noise current (1.0 pA/√Hz), and slew rate (1000 V/µs) give higher performance capabilities to these applications over previous voltage feedback designs.

With a settling time of 30 ns to 0.01% and 13 ns to 0.1%, the devices are an excellent choice for DAC I/V conversion. The same characteristics along with low harmonic distortion make them a good choice for ADC buffering/amplification. With superb linearity at relatively high signal frequencies, the AD8047 and AD8048 are ideal drivers for ADCs up to 12 bits.

Operation as a Video Line Driver

The AD8047 and AD8048 have been designed to offer outstanding performance as video line drivers. The important specifications of differential gain (0.01%) and differential phase (0.02°) meet the most exacting HDTV demands for driving video loads.

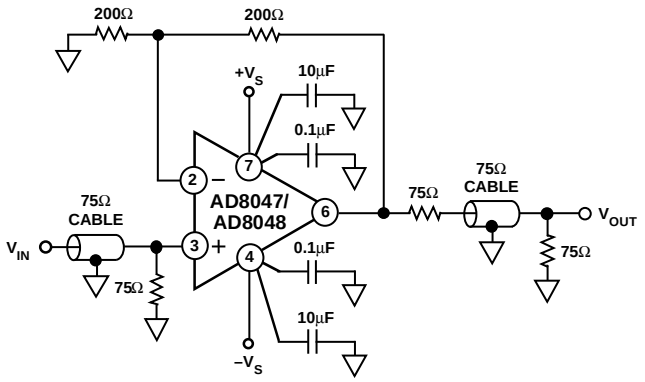


Figure 58. Video Line Driver

Active Filters

The wide bandwidth and low distortion of the AD8047 and AD8048 are ideal for the realization of higher bandwidth active filters. These characteristics, while being more common in many current feedback op amps, are offered in the AD8047 and AD8048 in a voltage feedback configuration. Many active filter configurations are not realizable with current feedback amplifiers.

A multiple feedback active filter requires a voltage feedback amplifier and is more demanding of op amp performance than other active filter configurations such as the Sallen-Key. In general, the amplifier should have a bandwidth that is at least ten times the bandwidth of the filter if problems due to phase shift of the amplifier are to be avoided.

Figure 59 is an example of a 20 MHz low pass multiple feedback active filter using an AD8048.

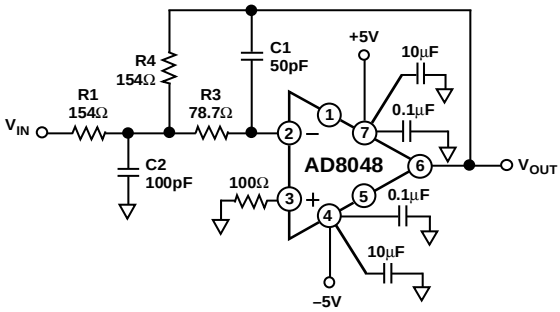


Figure 59. Active Filter Circuit

Choose:

F_O = Cutoff Frequency = 20 MHz

α = Damping Ratio = 1/Q = 2

H = Absolute Value of Circuit Gain = $\left|\frac{-R4}{R1}\right| = 1$

Then:

$$k = 2\pi \ F_O \ C1$$

$$C2 = \frac{4\,C1\,(H+1)}{\alpha^2}$$

$$R1 = \frac{\alpha}{2\,HK}$$

$$R3 = \frac{\alpha}{2\,K\,(H+1)}$$

$$R4 = H(R1)$$

A/D Converter Driver

As A/D converters move toward higher speeds with higher resolutions, there becomes a need for high performance drivers that will not degrade the analog signal to the converter. It is desirable from a system's standpoint that the A/D be the element in the signal chain that ultimately limits overall distortion. This places new demands on the amplifiers used to drive fast, high resolution A/Ds.

With high bandwidth, low distortion and fast settling time the AD8047 and AD8048 make high performance A/D drivers for advanced converters. Figure 60 is an example of an AD8047 used as an input driver for an AD872, a 12-bit, 10 MSPS A/D converter.

Layout Considerations

The specified high speed performance of the AD8047 and AD8048 requires careful attention to board layout and component selection. Proper RF design techniques and low pass parasitic component selection are mandatory

The PCB should have a ground plane covering all unused portions of the component side of the board to provide a low impedance path. The ground plane should be removed from the area near the input pins to reduce stray capacitance.

Chip capacitors should be used for the supply bypassing (see Figure 60). One end should be connected to the ground plane and the other within 1/8 inch of each power pin. An additional large (0.47 µF–10 µF) tantalum electrolytic capacitor should be connected in parallel, though not necessarily so close, to supply current for fast, large signal changes at the output.

The feedback resistor should be located close to the inverting input pin in order to keep the stray capacitance at this node to a minimum. Capacitance variations of less than 1 pF at the inverting input will significantly affect high speed performance.

Stripline design techniques should be used for long signal traces (greater than about 1 inch). These should be designed with a characteristic impedance of 50 Ω or 75 Ω and be properly terminated at each end.

Evaluation Board

An evaluation board for both the AD8047 and AD8048 is available that has been carefully laid out and tested to demonstrate that the specified high speed performance of the device can be realized. For ordering information, please refer to the Ordering Guide.

The layout of the evaluation board can be used as shown or serve as a guide for a board layout.

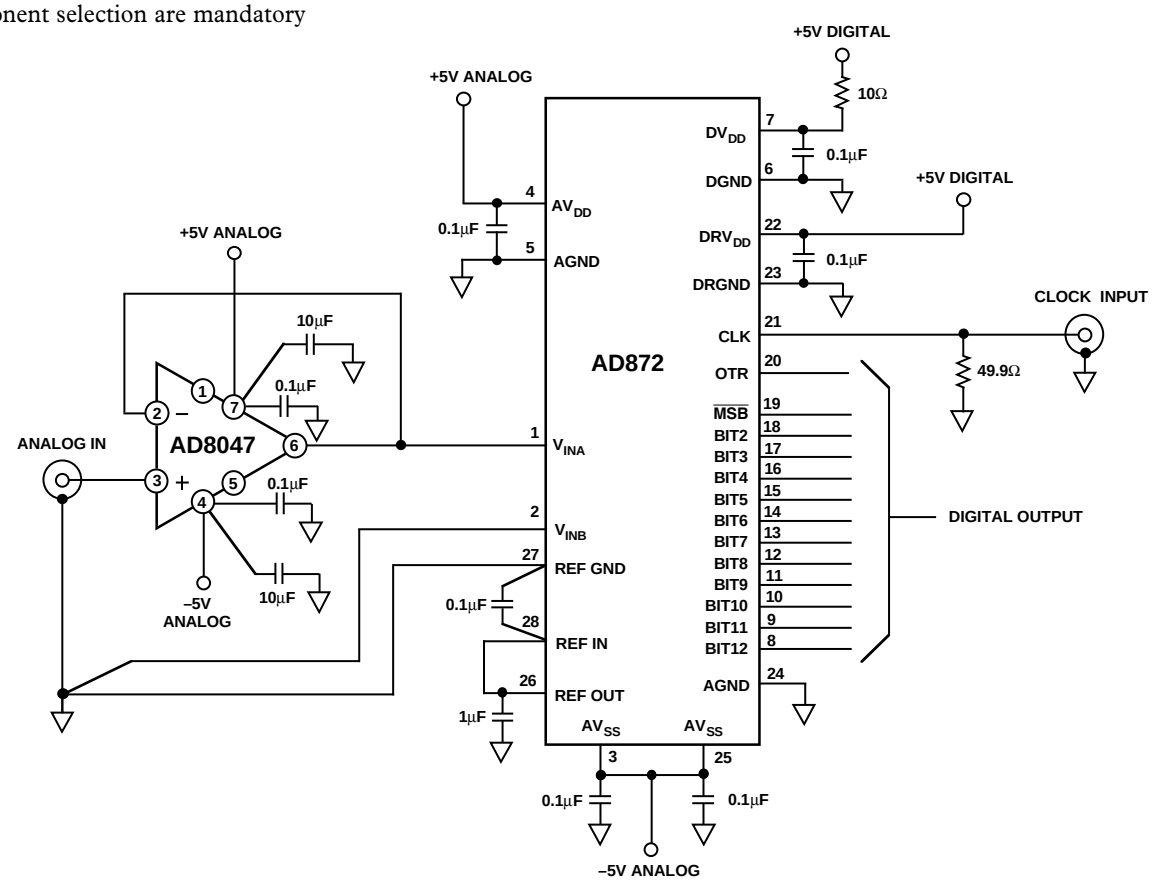
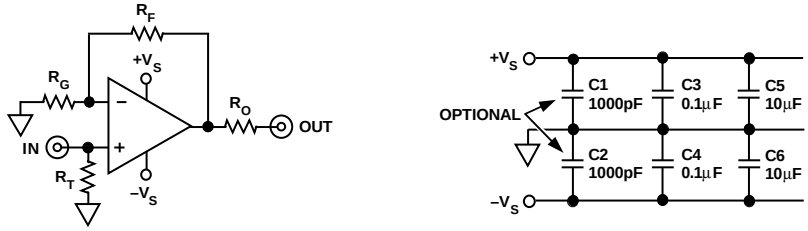


Figure 60. AD8047 Used as Driver for an AD872, a 12-Bit, 10 MSPS A/D Converter



Noninverting Configuration *Supply Bypassing*

Figure 61. Noninverting Configurations for Evaluation Boards

Table I.

	AD8047					AD8048			
Component	**–1**	**+1**	**+2**	**+10**	**+101**	**–1**	**+2**	**+10**	**+101**
R_F	200 Ω	66.5 Ω	1 kΩ	1 kΩ	1 kΩ	200 Ω	200 Ω	1 kΩ	1 kΩ
R_G	200 Ω	–	1 kΩ	110 Ω	10 Ω	200 Ω	200 Ω	110 Ω	10 Ω
R_O	49.9 Ω	49.9 Ω	49.9 Ω	49.9 Ω	49.9 Ω	49.9 Ω	49.9 Ω	49.9 Ω	49.9 Ω
R_S	–	0 Ω	0 Ω	0 Ω	0 Ω	–	0 Ω	0 Ω	0 Ω
R_T	66.5 Ω	49.9 Ω	49.9 Ω	49.9 Ω	49.9 Ω	66.5 Ω	49.9 Ω	49.9 Ω	49.9 Ω
Small Signal BW (–3 dB)	90 MHz	260 MHz	95 MHz	10 MHz	1 MHz	250 MHz	250 MHz	22 MHz	2 MHz

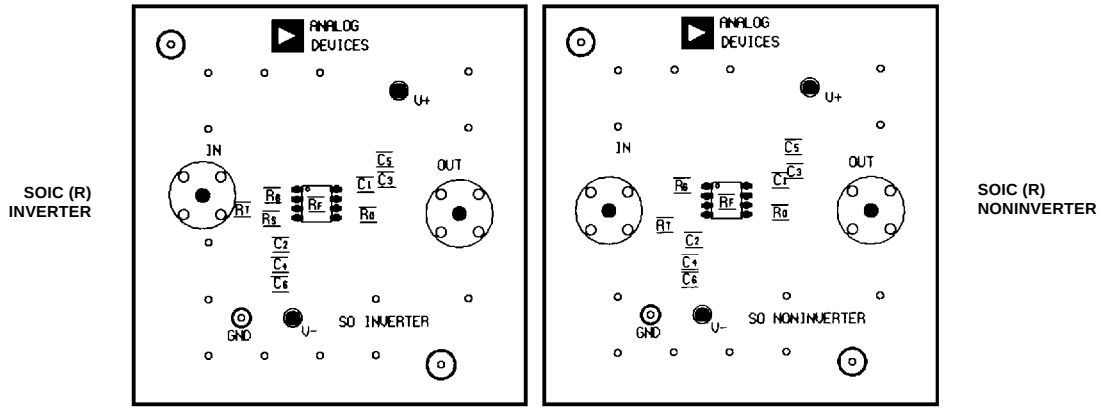


Figure 62. Evaluation Board Silkscreen (Top)

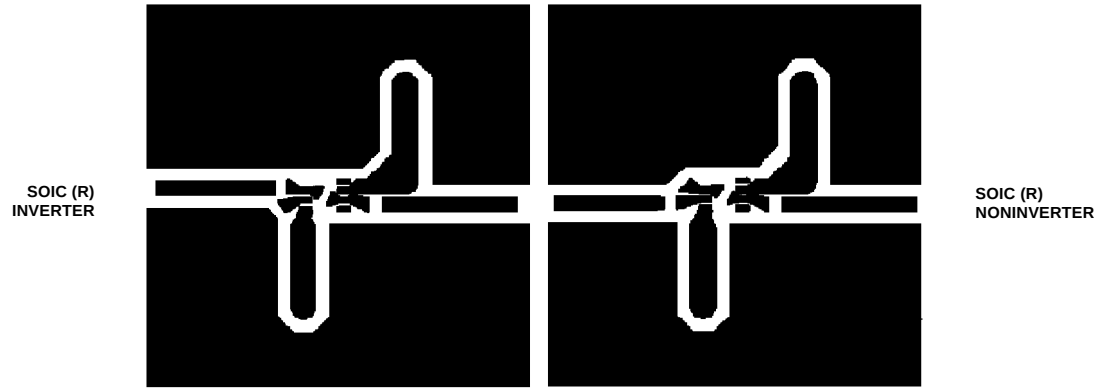


Figure 63. Board Layout (Solder Side)

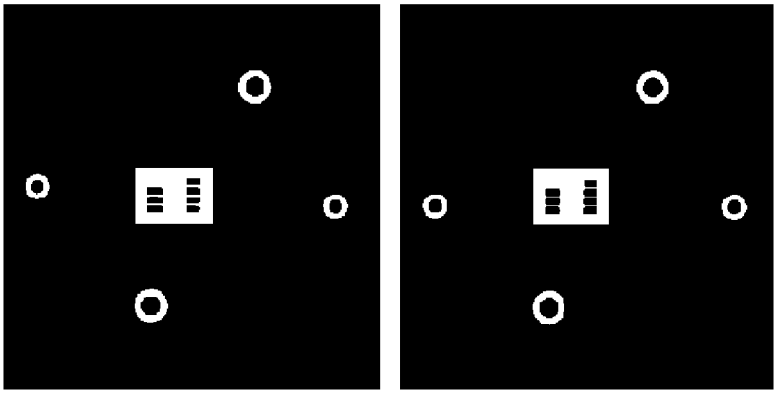
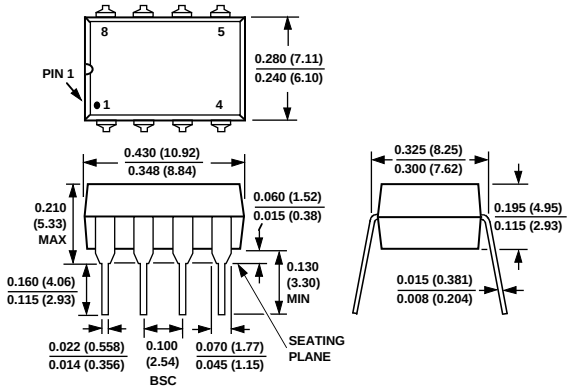


Figure 64. Board Layout (Component Side)

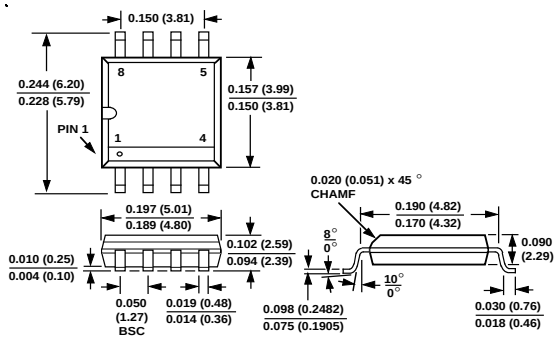
OUTLINE DIMENSIONS

Dimensions shown in inches and (mm).

8-Pin Plastic DIP
(N Package)



8-Pin Plastic SOIC
(R Package)



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