

# CLC416

## Dual Low-Power, 120MHz Op Amp

### General Description

The CLC416 is a dual, wideband (120MHz) op amp. The CLC416 consumes only 39mW per channel and can source or sink an output current of 60mA. These features make the CLC416 a versatile, high-speed solution for demanding applications that are sensitive to both power and cost.

Utilizing National's proven architectures, this dual current feedback amplifier surpasses the performance of alternative solutions and sets new standards for low power. This power-conserving dual op amp achieves low distortion with -80dBc and -80dBc second and third harmonics respectively. Many high source impedance applications will benefit from the CLC416's 6MΩ input impedance. And finally, designers will have a bipolar part with an exceptionally low 100nA non-inverting bias current.

With 0.1dB flatness to 30MHz and low differential gain and phase errors, the CLC416 is an ideal part for professional video processing and distribution. The 120MHz -3dB bandwidth ( $A_v = +2$ ) coupled with a 400V/μs slew rate also makes the CLC416 a perfect choice in cost-sensitive applications such as video monitors, fax machines, copiers, and CATV systems.

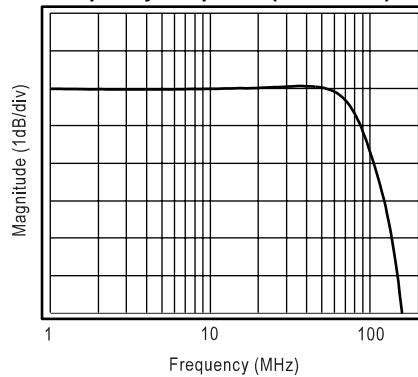
### Features

- 0.01%, 0.03°  $D_G$ ,  $D_\phi$
- Very low input bias current: 100nA
- High input impedance: 6MΩ
- 120MHz -3dB bandwidth ( $A_v = +2$ )
- Low power
- High output current: 60mA
- Low-cost

### Applications

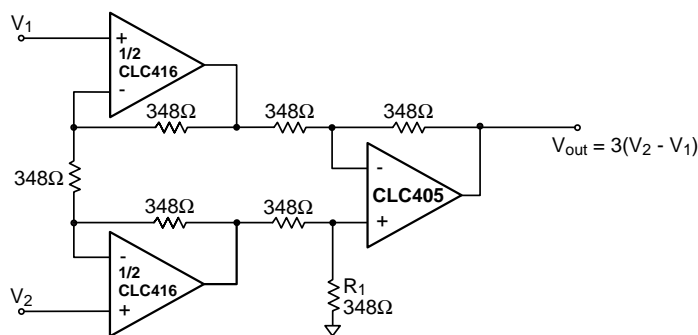
- Desktop video systems
- Video distribution
- Flash A/D driver
- High-speed driver
- High-source impedance applications
- Professional video processing
- High resolution monitors

Frequency Response ( $A_v = +2V/V$ )



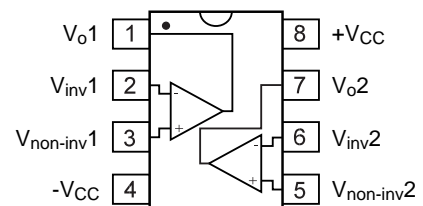
### Typical Application Diagram

#### Instrumentation Amplifier



### Pinout

#### DIP & SOIC



# CLC416 Electrical Characteristics ( $A_V = +2$ , $R_f = 348\Omega$ ; $V_{CC} = \pm 5V$ , $R_L = 100\Omega$ unless specified)

PARAMETERS	CONDITIONS	TYP	MIN/MAX RATINGS			UNITS	NOTES
Ambient Temperature	CLC416AJ	+25°C	+25°C	0 to 70°C	-40 to 85°C		
<b>FREQUENCY DOMAIN RESPONSE</b>							
-3dB bandwidth	$V_{out} < 1.0V_{pp}$	120	65	45	45	MHz	1
	$V_{out} < 5.0V_{pp}$	52	40	36	35	MHz	
$\pm 0.1$ dB bandwidth	$V_{out} < 1.0V_{pp}$	30	15			MHz	
gain flatness	$V_{out} < 1.0V_{pp}$						
peaking	DC to 200MHz	0.1	0.7	0.8	1.0	dB	
rolloff	<30MHz	0	0.3	0.6	0.6	dB	
linear phase deviation	<20MHz	0.3	0.6	0.7	0.7	deg	
differential gain	4.43MHz, $R_L = 150\Omega$	0.01	0.04	0.04	0.04	%	
differential phase	4.43MHz, $R_L = 150\Omega$	0.03	0.08	0.11	0.12	deg	
<b>TIME DOMAIN RESPONSE</b>							
rise and fall time	2V step	4.3	6.5	7.2	7.4	ns	
settling time to 0.05%	2V step	22	30	38	41	ns	
overshoot	2V step	3	12	12	12	%	
slew rate	$A_V = +2$ 2V step	400	300	260	250	V/ $\mu$ s	
	$A_V = -1$ 1V step	700				V/ $\mu$ s	
<b>DISTORTION AND NOISE RESPONSE</b>							
2 <sup>nd</sup> harmonic distortion	2V <sub>pp</sub> , 1MHz	-80				dBc	
3 <sup>rd</sup> harmonic distortion	2V <sub>pp</sub> , 1MHz	-80				dBc	
2 <sup>nd</sup> harmonic distortion	2V <sub>pp</sub> , 10MHz	-65	-55	-50	-47	dBc	
3 <sup>rd</sup> harmonic distortion	2V <sub>pp</sub> , 10MHz	-57	-50	-45	-45	dBc	
equivalent input noise							
voltage	>1MHz	5	6.3	6.6	6.7	nV/ $\sqrt$ Hz	
inverting current	>1MHz	12	15	16	17	pA/ $\sqrt$ Hz	
non-inverting current	>1MHz	3	3.8	4.0	4.2	pA/ $\sqrt$ Hz	
crosstalk, input referred	2V <sub>pp</sub> , 10MHz	72	66	66	66	dB	
<b>STATIC DC PERFORMANCE</b>							
input offset voltage		1	5	7	8	mV	A
average drift		30		50	50	$\mu$ V/ $^{\circ}$ C	
input bias current	non-inverting	100	900	1600	2800	nA	A
average drift		3		8	11	nA/ $^{\circ}$ C	
input bias current	inverting	1	5	6	8	$\mu$ A	A
average drift		17		40	45	nA/ $^{\circ}$ C	
power supply rejection ratio	DC	52	47	47	45	dB	
common-mode rejection ratio	DC	50	45	45	43	dB	
supply current per channel	$R_L = \infty$	3.9	4.5	4.6	4.9	mA	A
<b>MISCELLANEOUS PERFORMANCE</b>							
input resistance	non-inverting	6	3	2.4	1	M $\Omega$	
input capacitance	non-inverting	1	2	2	2	pF	
common mode input range		$\pm 2.2$	$\pm 1.8$	$\pm 1.7$	$\pm 1.5$	V	
output voltage range	$R_L = 100\Omega$	+3.5,-2.9	+3.1/-2.8	+2.9/-2.7	+2.4/-1.7	V	
output voltage range	$R_L = \infty$	+4.0,-3.4	+3.9/-3.3	+3.8/-3.2	+3.7/-2.8	V	
output current		60	44	38	20	mA	
output resistance, closed loop		0.06	0.2	0.25	0.4	$\Omega$	

Recommended gain range  $\pm 1$  to  $\pm 40V/V$

Transistor count = 110

Min/max ratings are based on product characterization and simulation. Individual parameters are tested as noted. Outgoing quality levels are determined from tested parameters.

## Absolute Maximum Ratings

supply voltage	$\pm 7V$
$I_{out}$ is short circuit protected to ground	
common-mode input voltage	$\pm V_{CC}$
maximum junction temperature	+175°C
storage temperature range	-65°C to +150°C
lead temperature (soldering 10 sec)	+300°C
ESD rating (human body model)	1000V

## Notes

- 1) At temps < 0°C, spec is guaranteed for  $R_L = 500\Omega$ .
- A) J-level: spec is 100% tested at +25°C.

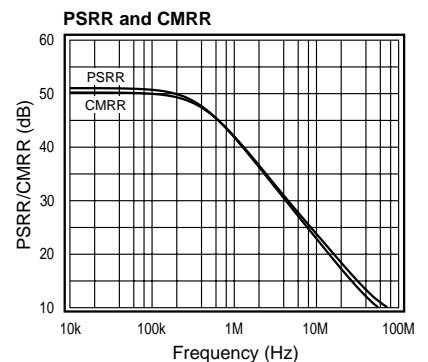
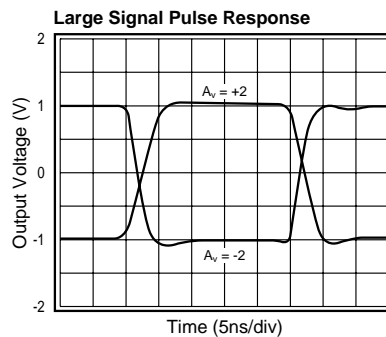
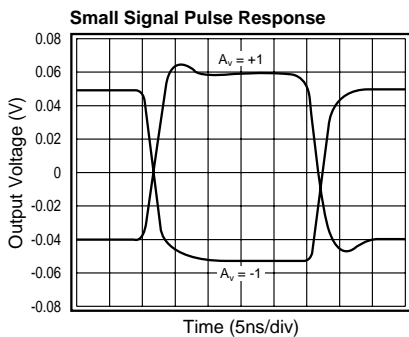
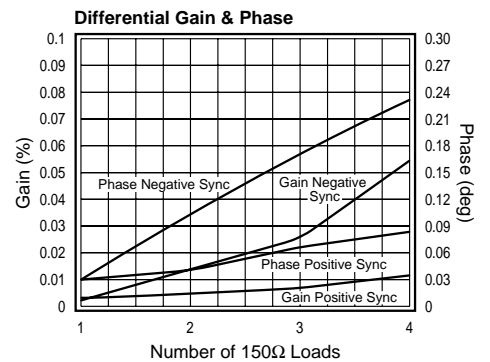
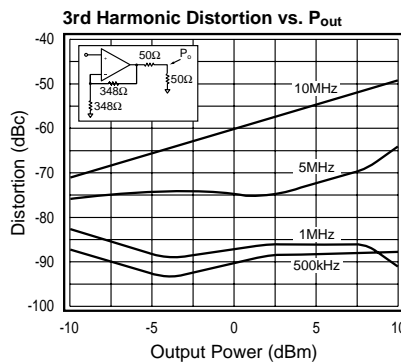
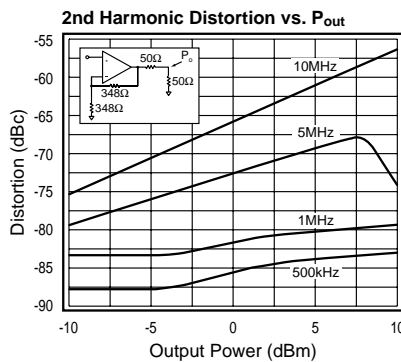
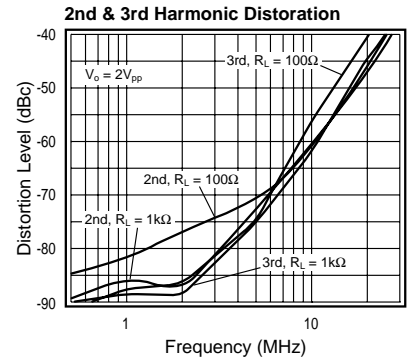
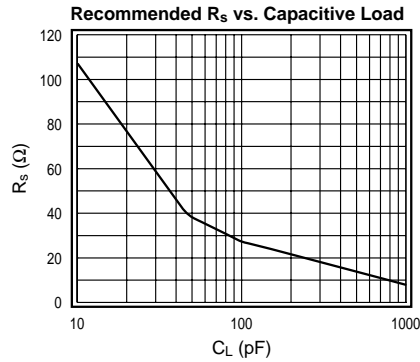
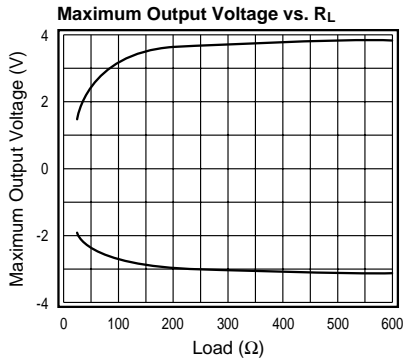
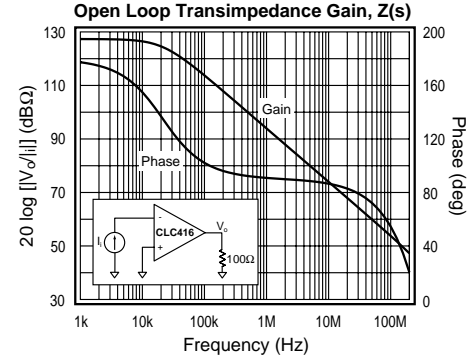
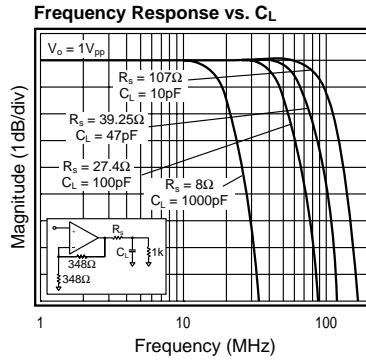
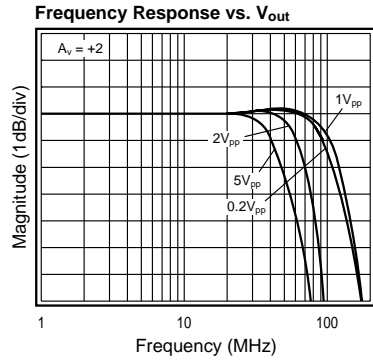
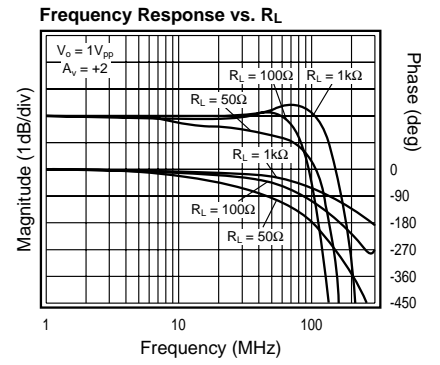
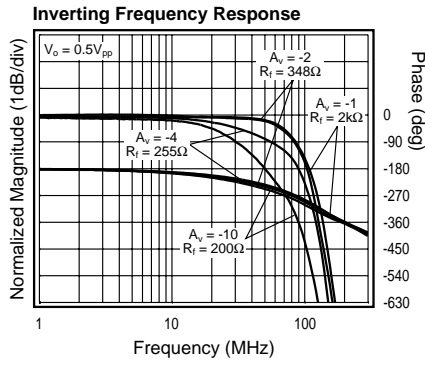
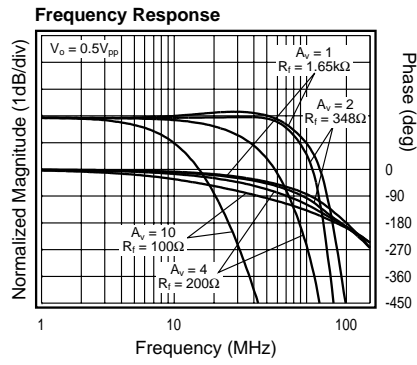
## Ordering Information

Model	Temperature Range	Description
CLC416AJP	-40°C to +85°C	8-pin PDIP
CLC416AJE	-40°C to +85°C	8-pin SOIC

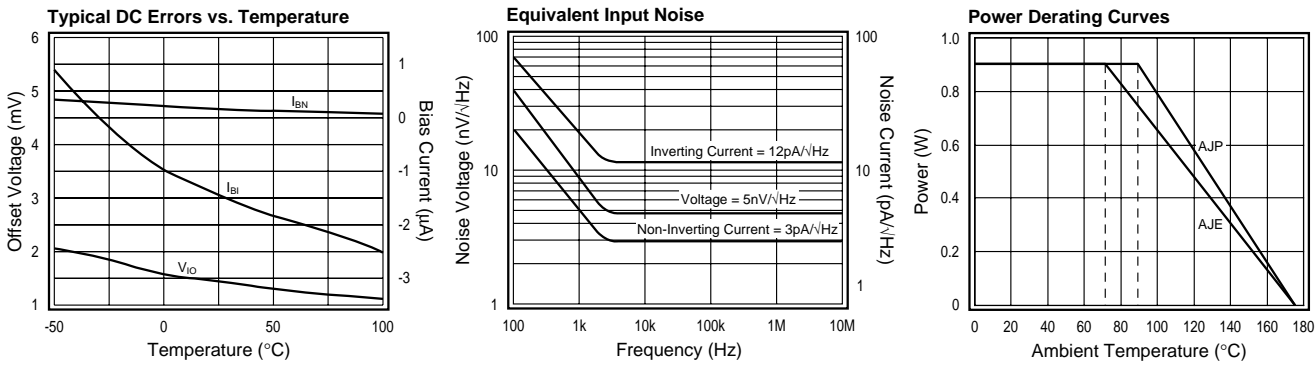
## Package Thermal Resistance

Package	$\theta_{JC}$	$\theta_{JA}$
Plastic (AJP)	80°C/W	95°C/W
Surface Mount (AJE)	95°C/W	115°C/W

# CLC416 Typical Performance Characteristics ( $V_{CC} = \pm 5V$ , $A_V = +2$ , $R_f = 348\Omega$ , $R_L = 100\Omega$ ; unless specified)



# CLC416 Typical Performance Characteristics ( $V_{CC} = \pm 5V$ , $A_v = +2$ , $R_f = 348\Omega$ , $R_L = 100\Omega$ ; unless specified)



## CLC416 OPERATION

### Description

The CLC416 is a dual current feedback amplifier with the following features:

- Differential gain and phase errors of 0.01% and 0.03° into a 150Ω load
- Low, 3.9mA, supply current per amplifier

The professional video quality differential gain and phase errors and low power capabilities of the CLC416 make this product a good choice for video applications.

### Gain

The non-inverting and inverting gain equations for the CLC416 are as follows:

$$\text{Non-inverting Gain: } 1 + \frac{R_f}{R_g}$$

$$\text{Inverting Gain: } -\frac{R_f}{R_g}$$

Where  $R_f$  is the feedback resistor and  $R_g$  is the gain setting resistor. Figure 1 shows the general non-inverting gain configuration including the recommended bypass capacitors.

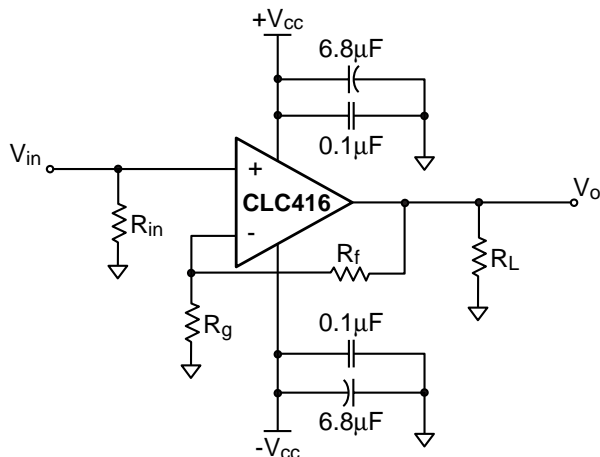


Figure 1: Recommended Non-Inverting Gain Circuit

### Feedback Resistor Selection

The feedback resistor,  $R_f$ , determines the loop gain and frequency response of a current feedback amplifier. Optimum performance of the CLC416, at a gain of +2V/V, is achieved with  $R_f$  equal to 348Ω. The frequency response plots in the typical performance section illustrate the recommended  $R_f$  for several gains. Within limits,  $R_f$  can be adjusted to optimize the frequency response.

- Decrease  $R_f$  to peak frequency response and extend bandwidth
- Increase  $R_f$  to roll off frequency response and reduce bandwidth

As a rule of thumb, if the recommended  $R_f$  is doubled, the bandwidth will be cut in half.

### Channel Matching

Channel matching and crosstalk efficiency are largely dependent on board layout. The layout of National's dual amplifier evaluation boards are designed to produce optimum channel matching and isolation. Typical channel matching for the CLC416 is shown in Figure 2.

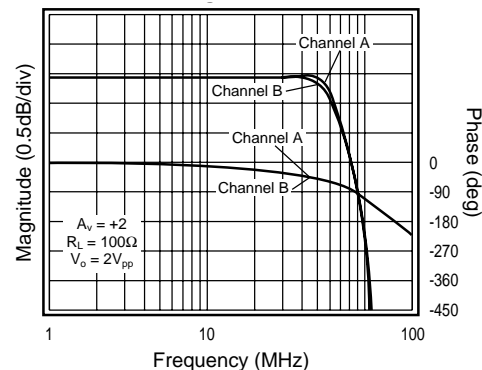
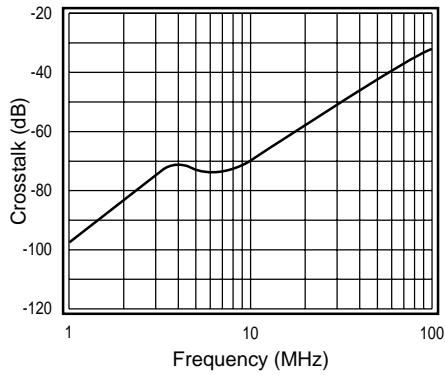


Figure 2: Channel Matching

The CLC416's channel-to-channel isolation is better than 70dB for input frequencies of 4MHz. Input referred crosstalk vs. frequency is illustrated in Figure 3.



**Figure 3: Input Referred Crosstalk vs. Frequency**

### Driving Cables and Capacitive Loads

When driving cables, double termination is used to prevent reflections. For capacitive load applications, a small series resistor at the output of the CLC416 will improve stability. The  $R_s$  vs. *Capacitive Load* plot, in the *Typical Performance* section, gives the recommended series resistance value for optimum flatness at various capacitive loads.

### Power Dissipation

The power dissipation of an amplifier can be described in two conditions:

- Quiescent Power Dissipation -  $P_Q$  (No Load Condition)
- Total Power Dissipation -  $P_T$  (with Load Condition)

The following steps can be taken to determine the power consumption for each CLC416 amplifier:

1. Determine the quiescent power  
 $P_Q = I_{CC} (V_{CC} - V_{EE})$
2. Determine the RMS power at the output stage  
 $P_O = (V_{CC} - V_{load}) (I_{load})$ , where  $V_{load}$  and  $I_{load}$  are the RMS voltage and current across the external load.
3. Determine the total RMS power  
 $P_T = P_Q + P_O$

Add the total RMS powers for both channels to determine the power dissipated by the dual.

The maximum power that the package can dissipate at a given temperature is illustrated in the *Power Derating* curves in the *Typical Performance* section. The power derating curve for any package can be derived by utilizing the following equation:

$$P = \frac{(175^\circ - T_{amb})}{\theta_{JA}}$$

where:  $T_{amb}$  = Ambient temperature ( $^\circ\text{C}$ )  
 $\theta_{JA}$  = Thermal resistance, from junction to ambient, for a given package ( $^\circ\text{C}/\text{W}$ )

### Layout Considerations

A proper printed circuit layout is essential for achieving high frequency performance. National provides

evaluation boards for the CLC416 (CLC730038 - DIP, CLC730036 - SOIC) and suggests their use as a guide for high frequency layout and as an aid for device testing and characterization.

Supply bypassing is required for best performance. The bypass capacitors provide a low impedance return current path at the supply pins. They also provide high frequency filtering on the power supply traces. Other layout factors play a major role in high frequency performance. The following are recommended as a basis for high frequency layout:

1. Include 6.8 $\mu\text{F}$  tantalum and 0.1 $\mu\text{F}$  ceramic capacitors on both supplies.
2. Place the 6.8 $\mu\text{F}$  capacitors within 0.75 inches of the power pins.
3. Place the 0.1 $\mu\text{F}$  capacitors within 0.1 inches of the power pins.
4. Remove the ground plane under and around the part, especially near the input and output pins to reduce parasitic capacitance.
5. Minimize all trace lengths to reduce series inductances.

Additional information is included in the evaluation board literature.

### SPICE Models

SPICE models provide a means to evaluate amplifier designs. Free SPICE models are available for National's monolithic amplifiers that:

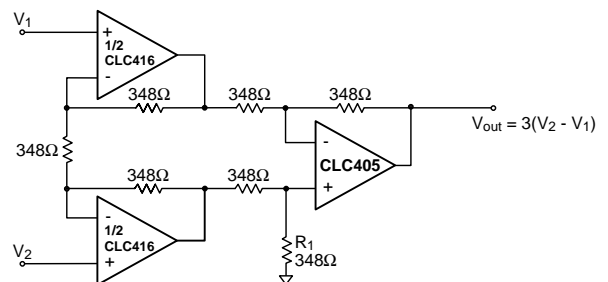
- Support Berkeley SPICE 2G and its many derivatives
- Reproduce typical DC, AC, Transient, and Noise performance
- Support room temperature simulations

The *readme* file that accompanies the diskette lists released models, and provides a list of modeled parameters. The application note OA-18, *Simulation SPICE Models for National's Op Amps*, contains schematics and a reproduction of the *readme* file.

## Applications Circuits

### Instrumentation Amplifier

An instrumentation circuit is shown on the front page and reproduced in Figure 4. The DC CMRR can be fine tuned by adjusting  $R_1$ .



**Figure 4: Instrumentation Amplifier**

### Differential Line Receiver

Figure 5 illustrates a Differential Line Receiver. The circuit will convert differential signals to single-ended signals.

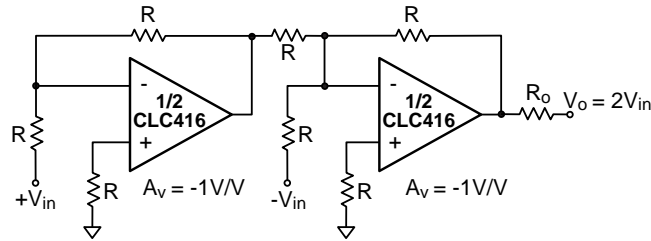


Figure 5: Differential Line Receiver

### Bandpass Filter

Figure 6 illustrates a low-sensitivity bandpass filter and design equations. This topology utilizes the CLC416's closely matched amplifiers to obtain low op-amp sensitivity at high frequencies. The CLC405 is used as a buffer to obtain low output impedance. The overall circuit gain is unity. For additional gain, the CLC405 can be configured as a non-inverting amplifier.

To design the filter, choose C and then determine values for R and R<sub>1</sub> based on the desired resonant frequency (f<sub>r</sub>) and Q factor.

Figure 7 illustrates a bandpass filter with Q = 10 and f<sub>r</sub> = 1MHz. The component values used are listed below:

- R<sub>1</sub> = 4.9kΩ
- R = 499Ω
- C = 330pF
- R<sub>f</sub> = 2kΩ

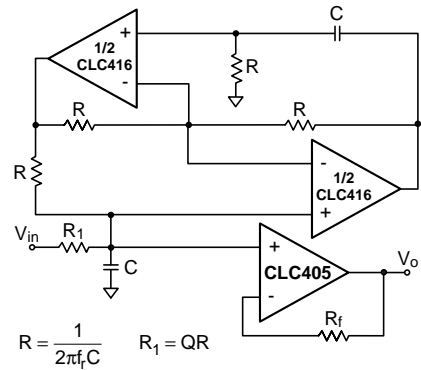


Figure 6: Bandpass Filter Topology

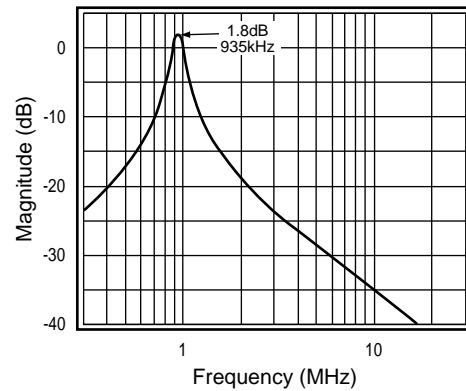


Figure 7: Bandpass Response

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