

# CLC452

## Single Supply, Low-Power, High Output, Current Feedback Amplifier

### General Description

The CLC452 has a new output stage that delivers high output drive current (100mA), but consumes minimal quiescent supply current (3.0mA) from a single 5V supply. Its current feedback architecture, fabricated in an advanced complementary bipolar process, maintains consistent performance over a wide range of gains and signal levels, and has a linear-phase response up to one half of the -3dB frequency.

The CLC452 offers superior dynamic performance with a 130MHz small-signal bandwidth, 400V/ $\mu$ s slew rate and 4.5ns rise/fall times ( $2V_{step}$ ). The combination of low quiescent power, high output current drive, and high-speed performance make the CLC452 well suited for many battery-powered personal communication/computing systems.

The ability to drive low-impedance, highly capacitive loads, makes the CLC452 ideal for single ended cable applications. It also drives low impedance loads with minimum distortion. The CLC452 will drive a 100 $\Omega$  load with only -75/-74dBc second/third harmonic distortion ( $A_v = +2$ ,  $V_{out} = 2V_{pp}$ ,  $f = 1\text{MHz}$ ). With a 25 $\Omega$  load, and the same conditions, it produces only -65/-77dBc second/third harmonic distortion. It is also optimized for driving high currents into single-ended transformers and coils.

When driving the input of high-resolution A/D converters, the CLC452 provides excellent -78/-85dBc second/third harmonic distortion ( $A_v = +2$ ,  $V_{out} = 2V_{pp}$ ,  $f = 1\text{MHz}$ ,  $R_L = 1\text{k}\Omega$ ) and fast settling time.

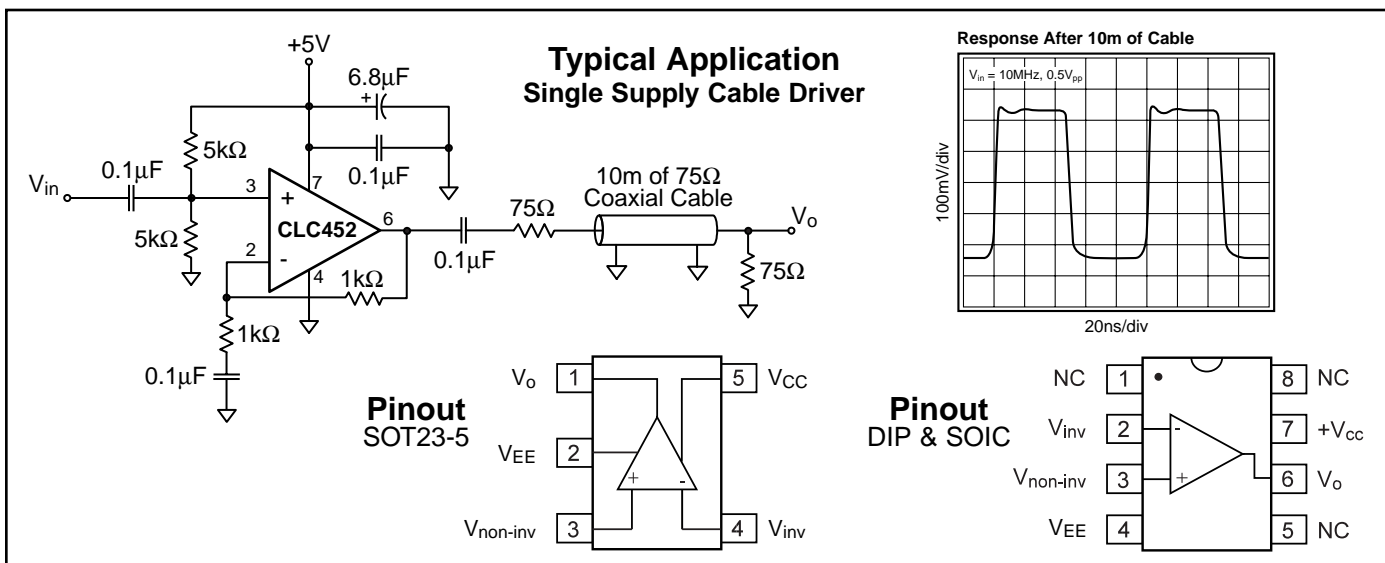
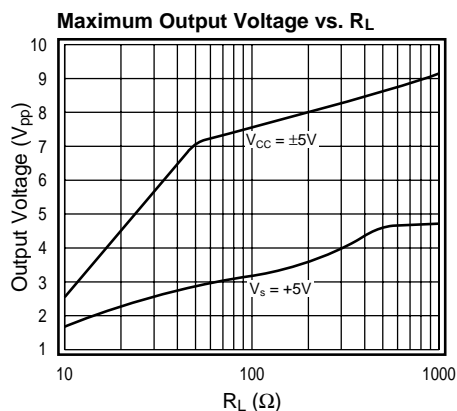
Available in SOT23-5, the CLC452 is ideal for applications where space is critical.

### Features

- 100mA output current
- 3.0mA supply current
- 130MHz bandwidth ( $A_v = +2$ )
- -78/-85dBc HD2/HD3 (1MHz)
- 25ns settling to 0.05%
- 400V/ $\mu$ s slew rate
- Stable for capacitive loads up to 1000pF
- Single 5V to  $\pm 5\text{V}$  supplies
- Available in Tiny SOT23-5 package

### Applications

- Coaxial cable driver
- Twisted pair driver
- Transformer/Coil Driver
- High capacitive load driver
- Video line driver
- Portable/battery-powered applications
- A/D driver



## +5V Electrical Characteristics ( $A_v = +2$ , $R_f = 1k\Omega$ , $R_L = 100\Omega$ , $V_s = +5V^1$ , $V_{cm} = V_{EE} + (V_s/2)$ , $R_L$ tied to $V_{cm}$ , unless specified)

PARAMETERS	CONDITIONS	TYP	MIN/MAX RATINGS			UNITS	NOTES
			+25°C	0 to 70°C	-40 to 85°C		
Ambient Temperature	CLC452AJ	+25°C	+25°C	0 to 70°C	-40 to 85°C		
<b>FREQUENCY DOMAIN RESPONSE</b>							
-3dB bandwidth	$V_o = 0.5V_{pp}$	130	95	90	85	MHz	
	$V_o = 2.0V_{pp}$	95	80	77	75	MHz	
-0.1dB bandwidth	$V_o = 0.5V_{pp}$	30	25	20	20	MHz	
gain peaking	<200MHz, $V_o = 0.5V_{pp}$	0	0.5	0.9	1.0	dB	
gain rolloff	<30MHz, $V_o = 0.5V_{pp}$	0.1	0.3	0.3	0.3	dB	
linear phase deviation	<30MHz, $V_o = 0.5V_{pp}$	0.1	0.2	0.3	0.3	deg	
<b>TIME DOMAIN RESPONSE</b>							
rise and fall time	2V step	4.5	6.0	6.4	6.8	ns	
settling time to 0.05%	1V step	25	—	—	—	ns	
overshoot	2V step	11	15	18	18	%	
slew rate	2V step	400	300	275	260	V/ $\mu$ s	
<b>DISTORTION AND NOISE RESPONSE</b>							
2 <sup>nd</sup> harmonic distortion	2V <sub>pp</sub> , 1MHz	-75	-69	-67	-67	dBc	
	2V <sub>pp</sub> , 1MHz; $R_L = 1k\Omega$	-78	-70	-68	-68	dBc	
	2V <sub>pp</sub> , 5MHz	-65	-58	-56	-56	dBc	
3 <sup>rd</sup> harmonic distortion	2V <sub>pp</sub> , 1MHz	-74	-70	-68	-68	dBc	
	2V <sub>pp</sub> , 1MHz; $R_L = 1k\Omega$	-85	-75	-73	-73	dBc	
	2V <sub>pp</sub> , 5MHz	-60	-55	-53	-53	dBc	
equivalent input noise voltage ( $e_{ni}$ )	>1MHz	2.8	3.5	3.8	3.8	nV/ $\sqrt$ Hz	
non-inverting current ( $i_{bn}$ )	>1MHz	7.5	10	11	11	pA/ $\sqrt$ Hz	
inverting current ( $i_{bi}$ )	>1MHz	10.5	14	15	15	pA/ $\sqrt$ Hz	
<b>STATIC DC PERFORMANCE</b>							
input offset voltage		1	4	6	6	mV	A
average drift		8	—	—	—	$\mu$ V/°C	
input bias current (non-inverting)		6	18	22	24	$\mu$ A	A
average drift		40	—	—	—	nA/°C	
input bias current (inverting)		6	14	16	17	$\mu$ A	A
average drift		25	—	—	—	nA/°C	
power supply rejection ratio	DC	48	45	43	43	dB	
common-mode rejection ratio	DC	51	48	46	46	dB	
supply current	$R_L = \infty$	3.0	3.4	3.6	3.6	mA	A
<b>MISCELLANEOUS PERFORMANCE</b>							
input resistance (non-inverting)		0.39	0.28	0.25	0.25	M $\Omega$	
input capacitance (non-inverting)		1.5	2.3	2.3	2.3	pF	
input voltage range, High		4.2	4.1	4.0	4.0	V	
input voltage range, Low		0.8	0.9	1.0	1.0	V	
output voltage range, High	$R_L = 100\Omega$	4.0	3.9	3.8	3.8	V	
output voltage range, Low	$R_L = 100\Omega$	1.0	1.1	1.2	1.2	V	
output voltage range, High	$R_L = \infty$	4.1	4.0	4.0	3.9	V	
output voltage range, Low	$R_L = \infty$	0.9	1.0	1.0	1.1	V	
output current		100	80	65	40	mA	B
output resistance, closed loop	DC	70	105	105	140	m $\Omega$	

Min/max ratings are based on product characterization and simulation. Individual parameters are tested as noted. Outgoing quality levels are determined from tested parameters.

### Notes

- A) J-level: spec is 100% tested at +25°C.  
 B) The short circuit current can exceed the maximum safe output current.  
 1)  $V_s = V_{CC} - V_{EE}$

### Absolute Maximum Ratings

supply voltage ( $V_{CC} - V_{EE}$ )	+14V
output current (see note C)	140mA
common-mode input voltage	$V_{EE}$ to $V_{CC}$
maximum junction temperature	+150°C
storage temperature range	-65°C to +150°C
lead temperature (soldering 10 sec)	+300°C
ESD rating (human body model)	500V

### Reliability Information

Transistor Count	49
MTBF (based on limited test data)	31Mhr

## ±5V Electrical Characteristics (A<sub>v</sub> = +2, R<sub>f</sub> = 1kΩ, R<sub>L</sub> = 100Ω, V<sub>CC</sub> = ±5V, unless specified)

PARAMETERS	CONDITIONS	TYP	GUARANTEED MIN/MAX			UNITS	NOTES
			+25°C	+25°C	0 to 70°C		
Ambient Temperature	CLC452AJ	+25°C	+25°C	0 to 70°C	-40 to 85°C		
<b>FREQUENCY DOMAIN RESPONSE</b>							
-3dB bandwidth	V <sub>o</sub> = 1.0V <sub>pp</sub>	160	135	120	115	MHz	
	V <sub>o</sub> = 4.0V <sub>pp</sub>	75	60	57	55	MHz	
-0.1dB bandwidth	V <sub>o</sub> = 1.0V <sub>pp</sub>	30	25	25	20	MHz	
gain peaking	<200MHz, V <sub>o</sub> = 1.0V <sub>pp</sub>	0	0.5	0.9	1.0	dB	
gain rolloff	<30MHz, V <sub>o</sub> = 1.0V <sub>pp</sub>	0.1	0.2	0.3	0.3	dB	
linear phase deviation	<30MHz, V <sub>o</sub> = 1.0V <sub>pp</sub>	0.1	0.2	0.3	0.3	deg	
differential gain	NTSC, R <sub>L</sub> =150Ω	0.05	–	–	–	%	
differential phase	NTSC, R <sub>L</sub> =150Ω	0.08	–	–	–	deg	
<b>TIME DOMAIN RESPONSE</b>							
rise and fall time	2V step	3.2	4.2	4.5	5.0	ns	
settling time to 0.05%	2V step	20	–	–	–	ns	
overshoot	2V step	8	12	15	15	%	
slew rate	2V step	540	400	370	350	V/μs	
<b>DISTORTION AND NOISE RESPONSE</b>							
2 <sup>nd</sup> harmonic distortion	2V <sub>pp</sub> , 1MHz	-77	-71	-69	-69	dBc	
	2V <sub>pp</sub> , 1MHz; R <sub>L</sub> = 1kΩ	-78	-72	-70	-70	dBc	
	2V <sub>pp</sub> , 5MHz	-69	-63	-61	-61	dBc	
3 <sup>rd</sup> harmonic distortion	2V <sub>pp</sub> , 1MHz	-72	-68	-66	-66	dBc	
	2V <sub>pp</sub> , 1MHz; R <sub>L</sub> = 1kΩ	-90	-80	-78	-78	dBc	
	2V <sub>pp</sub> , 5MHz	-58	-54	-52	-52	dBc	
equivalent input noise							
voltage (e <sub>ni</sub> )	>1MHz	2.8	3.5	3.8	3.8	nV/√Hz	
non-inverting current (i <sub>bn</sub> )	>1MHz	7.5	10	11	11	pA/√Hz	
inverting current (i <sub>bi</sub> )	>1MHz	10.5	14	15	15	pA/√Hz	
<b>STATIC DC PERFORMANCE</b>							
input offset voltage		1	6	8	8	mV	
average drift		10	–	–	–	μV/°C	
input bias current (non-inverting)		3	18	23	25	μA	
average drift		40	–	–	–	nA/°C	
input bias current (inverting)		13	24	31	31	μA	
average drift		30	–	–	–	nA/°C	
power supply rejection ratio	DC	48	45	43	43	dB	
common-mode rejection ratio	DC	53	50	48	48	dB	
supply current	R <sub>L</sub> = ∞	3.2	3.8	4.0	4.0	mA	
<b>MISCELLANEOUS PERFORMANCE</b>							
input resistance (non-inverting)		0.52	0.35	0.30	0.30	MΩ	
input capacitance (non-inverting)		1.2	1.8	1.8	1.8	pF	
common-mode input range		±4.2	±4.1	±4.1	±4.0	V	
output voltage range	R <sub>L</sub> = 100Ω	±3.8	±3.6	±3.6	±3.5	V	
output voltage range	R <sub>L</sub> = ∞	±4.0	±3.8	±3.8	±3.7	V	
output current		130	100	80	50	mA	B
output resistance, closed loop	DC	60	90	90	120	mΩ	

### Notes

B) The short circuit current can exceed the maximum safe output current.

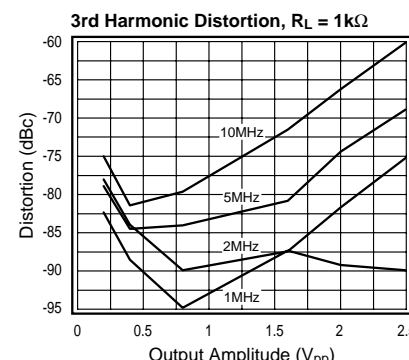
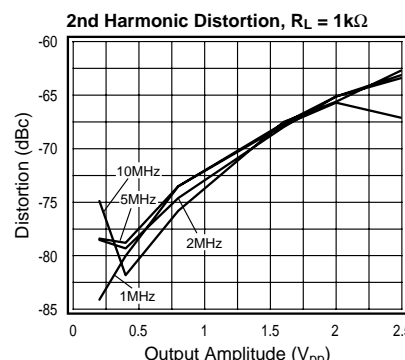
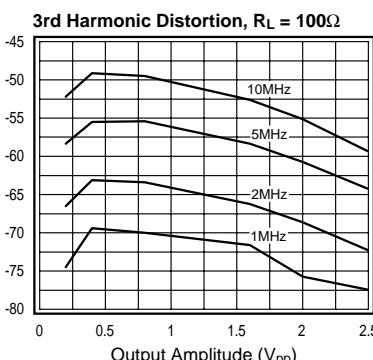
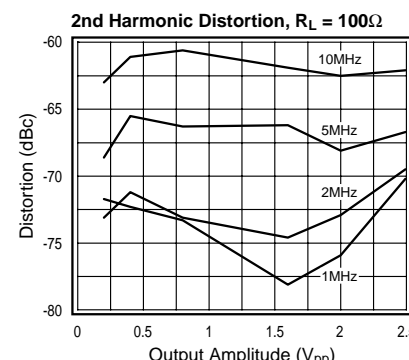
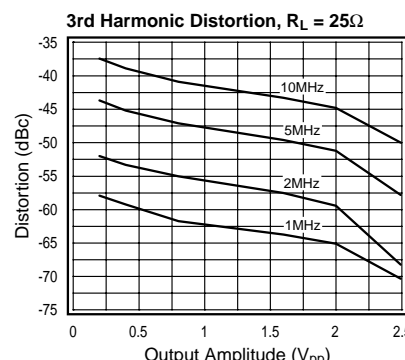
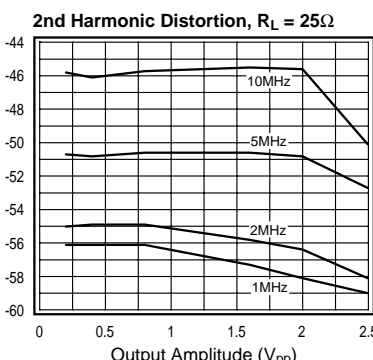
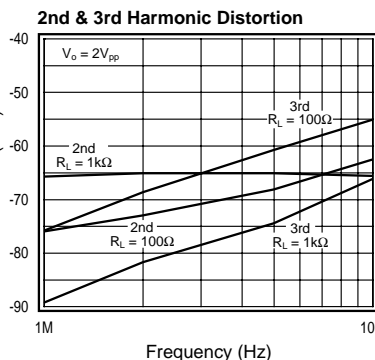
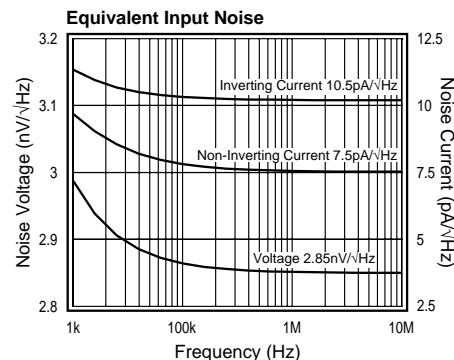
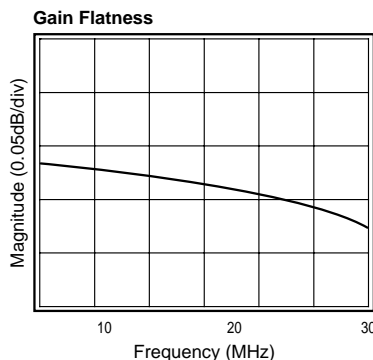
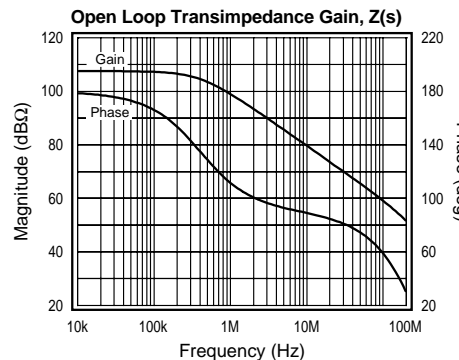
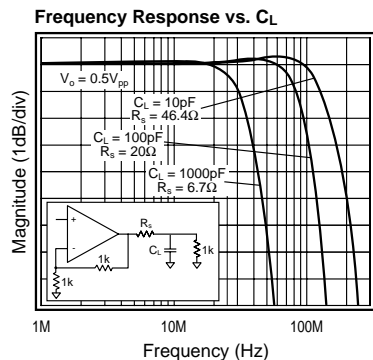
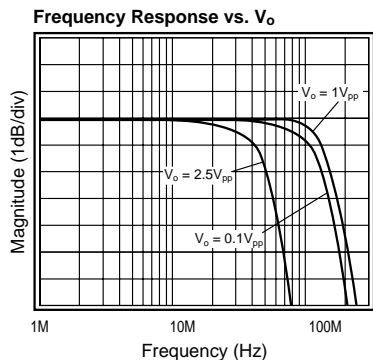
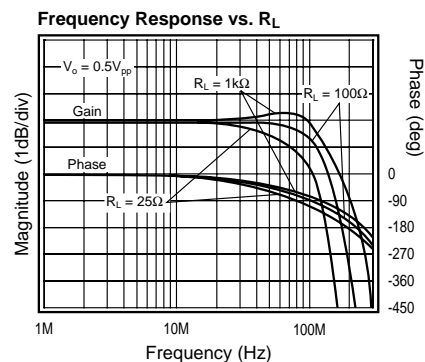
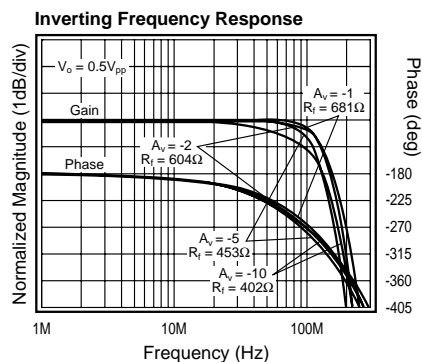
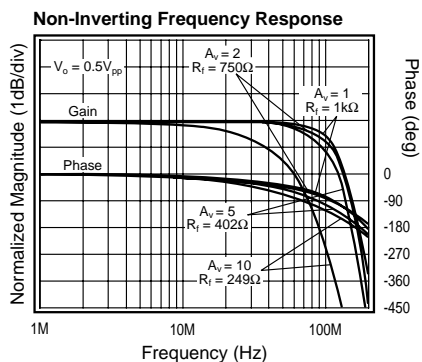
### Package Thermal Resistance

Package	θ <sub>JC</sub>	θ <sub>JA</sub>
Plastic (AJP)	105°C/W	155°C/W
Surface Mount (AJE)	95°C/W	175°C/W
Surface Mount (AJM5)	140°C/W	210°C/W
Dice (ALC)	25°C/W	–
CerDIP (A8B)	70°C/W	215°C/W

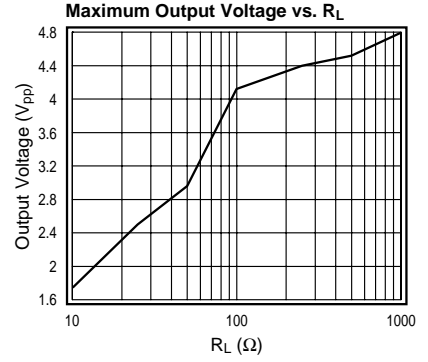
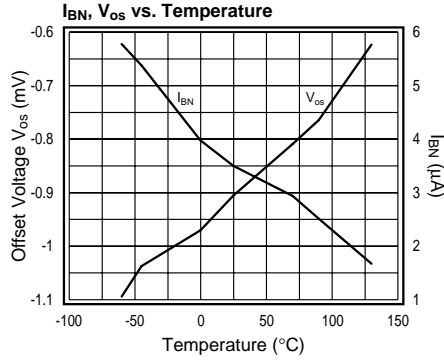
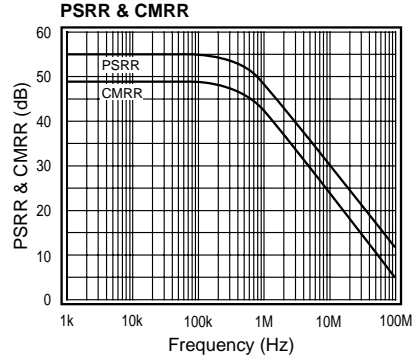
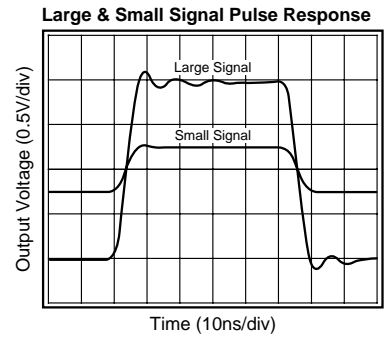
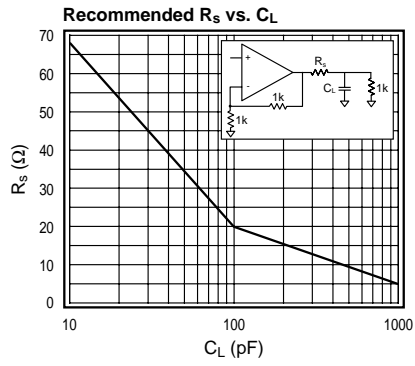
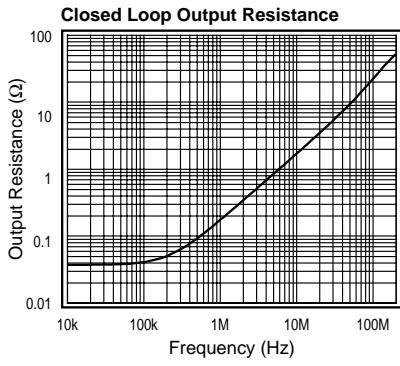
### Ordering Information

Model	Temperature Range	Description
CLC452AJP	-40°C to +85°C	8-pin PDIP
CLC452AJE	-40°C to +85°C	8-pin SOIC
CLC452AJM5	-40°C to +85°C	5-pin SOT
CLC452ALC	-40°C to +85°C	dice
CLC452A8B	-55°C to +175°C	8-pin CerDIP, MIL-STD-883
CLC452ALC	-55°C to +175°C	dice, MIL-STD-883

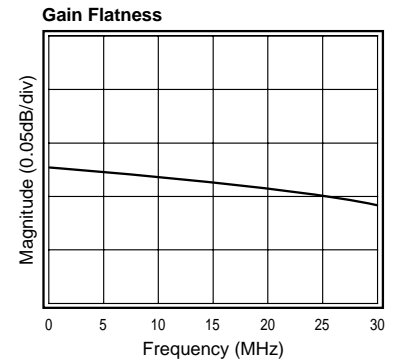
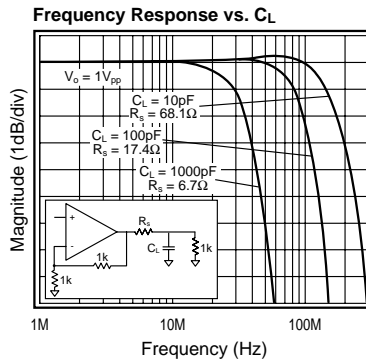
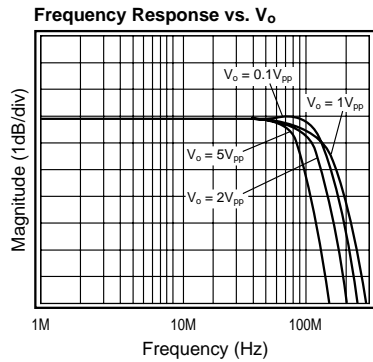
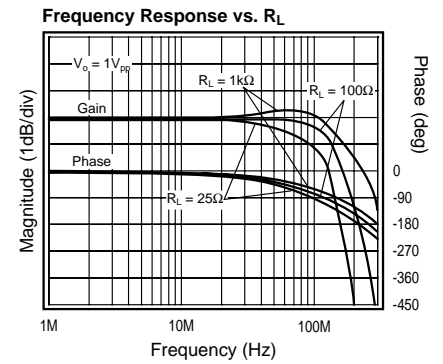
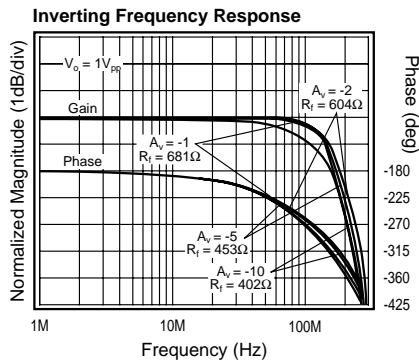
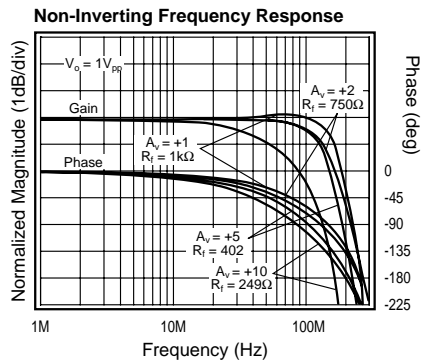
**+5V Typical Performance** ( $A_v = +2$ ,  $R_f = 1k\Omega$ ,  $R_L = 100\Omega$ ,  $V_s = +5V^1$ ,  $V_{cm} = V_{EE} + (V_s/2)$ ,  $R_L$  tied to  $V_{cm}$ , unless specified)



**+5V Typical Performance** ( $A_v = +2$ ,  $R_f = 1k\Omega$ ,  $R_L = 100\Omega$ ,  $V_s = +5V^1$ ,  $V_{cm} = V_{EE} + (V_s/2)$ ,  $R_L$  tied to  $V_{cm}$ , unless specified)

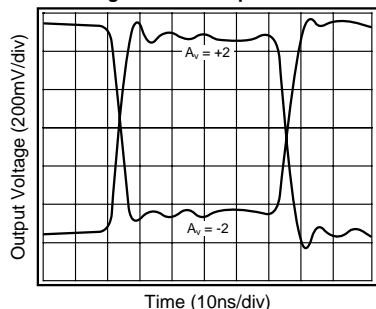


**±5V Typical Performance** ( $A_v = +2$ ,  $R_f = 1k\Omega$ ,  $R_L = 100\Omega$ ,  $V_{CC} = \pm 5V$ , unless specified)

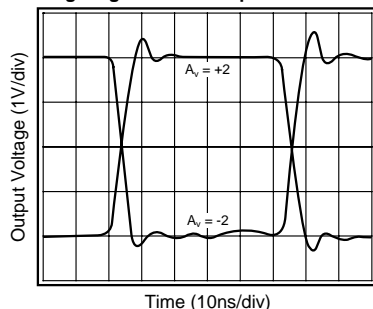


# ±5V Typical Performance ( $A_v = +2$ , $R_f = 1k\Omega$ , $R_L = 100\Omega$ , $V_{CC} = \pm 5V$ , unless specified)

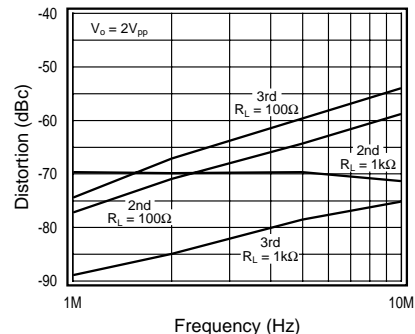
**Small Signal Pulse Response**



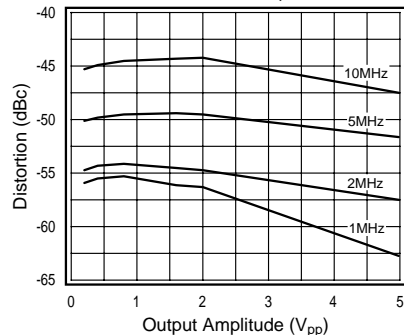
**Large Signal Pulse Response**



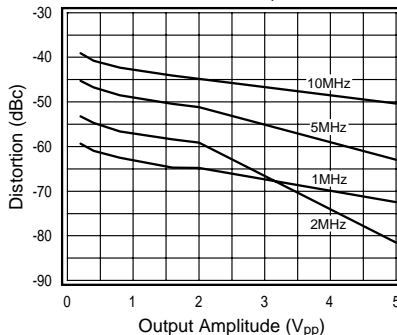
**2nd & 3rd Harmonic Distortion**



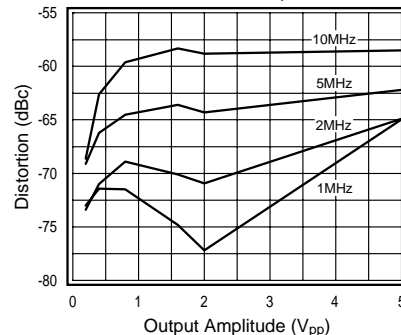
**2nd Harmonic Distortion,  $R_L = 25\Omega$**



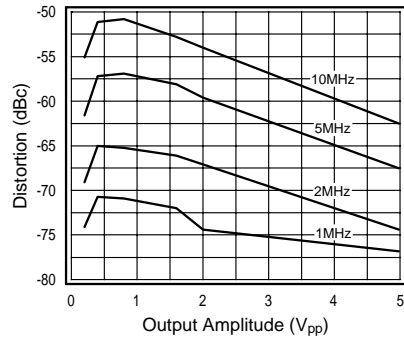
**3rd Harmonic Distortion,  $R_L = 25\Omega$**



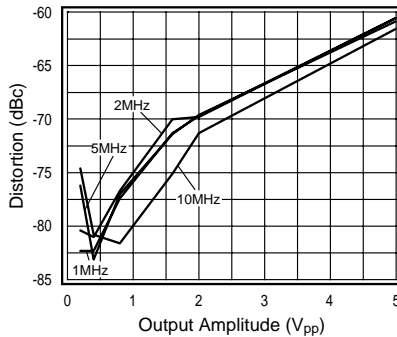
**2nd Harmonic Distortion,  $R_L = 100\Omega$**



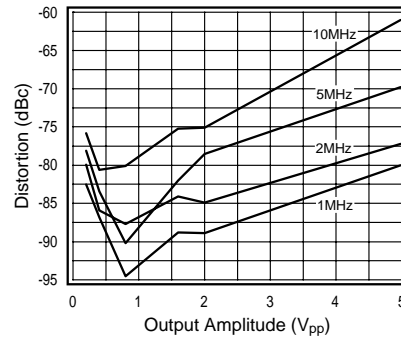
**3rd Harmonic Distortion,  $R_L = 100\Omega$**



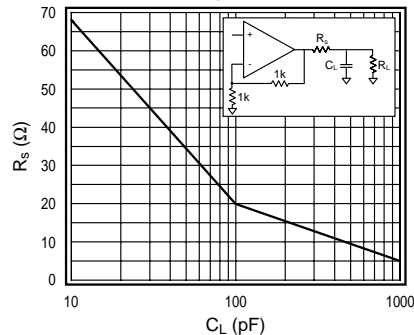
**2nd Harmonic Distortion,  $R_L = 1k\Omega$**



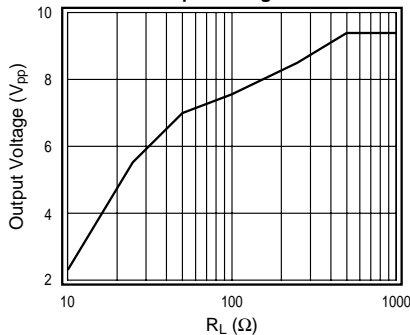
**3rd Harmonic Distortion,  $R_L = 1k\Omega$**



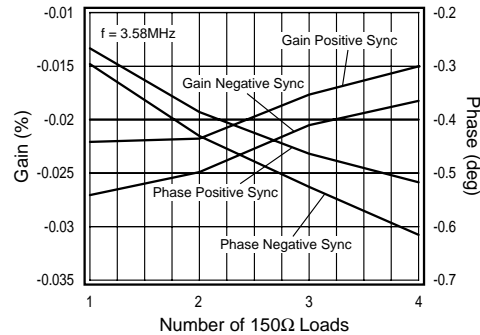
**Recommended  $R_s$  vs.  $C_L$**



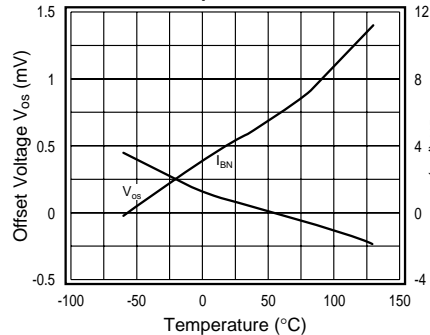
**Maximum Output Voltage vs.  $R_L$**



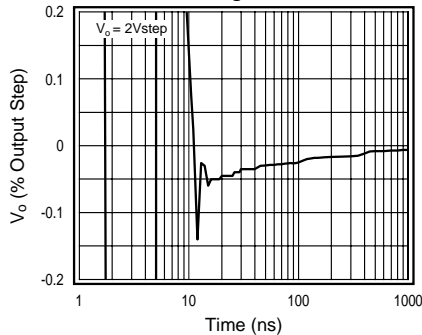
**Differential Gain & Phase**



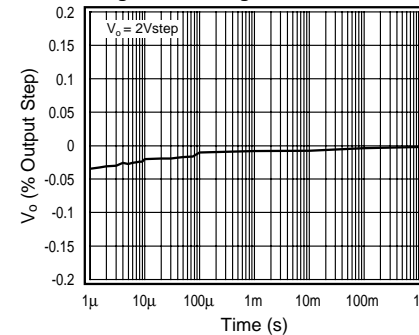
**$I_{BN}$ ,  $V_{os}$  vs. Temperature**



**Short Term Settling Time**



**Long Term Settling Time**





# CLC452 Operation

The CLC452 is a current feedback amplifier built in an advanced complementary bipolar process. The CLC452 operates from a single 5V supply or dual  $\pm 5V$  supplies. Operating from a single supply, the CLC452 has the following features:

- Provides 100mA of output current while consuming 15mW of power
- Offers low -78/-85dB 2nd and 3rd harmonic distortion
- Provides BW > 80MHz and 1MHz distortion < -70dBc at  $V_o = 2.0V_{pp}$

The CLC452 performance is further enhanced in  $\pm 5V$  supply applications as indicated in the  **$\pm 5V$  Electrical Characteristics** table and  **$\pm 5V$  Typical Performance** plots.

## Current Feedback Amplifiers

Some of the key features of current feedback technology are:

- Independence of AC bandwidth and voltage gain
- Inherently stable at unity gain
- Adjustable frequency response with feedback resistor
- High slew rate
- Fast settling

Current feedback operation can be described using a simple equation. The voltage gain for a non-inverting or inverting current feedback amplifier is approximated by Equation 1.

$$\frac{V_o}{V_{in}} = \frac{A_v}{1 + \frac{R_f}{Z(j\omega)}} \quad \text{Equation 1}$$

where:

- $A_v$  is the closed loop DC voltage gain
- $R_f$  is the feedback resistor
- $Z(j\omega)$  is the CLC452's open loop transimpedance gain
- $\frac{Z(j\omega)}{R_f}$  is the loop gain

The denominator of Equation 1 is approximately equal to 1 at low frequencies. Near the -3dB corner frequency, the interaction between  $R_f$  and  $Z(j\omega)$  dominates the circuit performance. The value of the feedback resistor has a large affect on the circuits performance. Increasing  $R_f$  has the following affects:

- Decreases loop gain
- Decreases bandwidth
- Reduces gain peaking
- Lowers pulse response overshoot
- Affects frequency response phase linearity

Refer to the **Feedback Resistor Selection** section for more details on selecting a feedback resistor value.

# CLC452 Design Information

## Single Supply Operation ( $V_{CC} = +5V, V_{EE} = GND$ )

The specifications given in the  **$\pm 5V$  Electrical Characteristics** table for single supply operation are measured with a common mode voltage ( $V_{cm}$ ) of 2.5V.  $V_{cm}$  is the voltage around which the inputs are applied and the output voltages are specified.

Operating from a single +5V supply, the Common Mode Input Range (CMIR) of the CLC452 is typically +0.8V to +4.2V. The typical output range with  $R_L = 100\Omega$  is +1.0V to +4.0V.

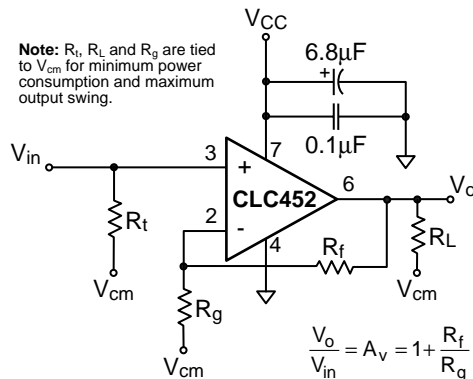


Figure 1: Non-Inverting Configuration

For single supply DC coupled operation, keep input signal levels above 0.8V DC. For input signals that drop below 0.8V DC, AC coupling and level shifting the signal are recommended. The non-inverting and inverting configurations for both input conditions are illustrated in the following 2 sections.

## DC Coupled Single Supply Operation

Figures 1 and 2 show the recommended non-inverting and inverting configurations for input signals that remain above 0.8V DC.

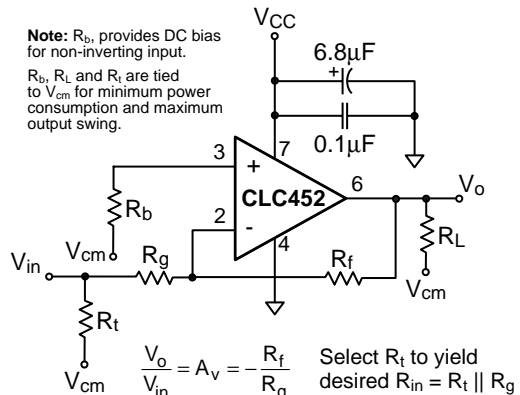
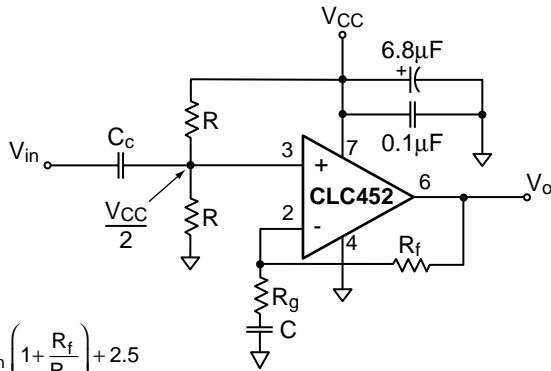


Figure 2: Inverting Configuration

### AC Coupled Single Supply Operation

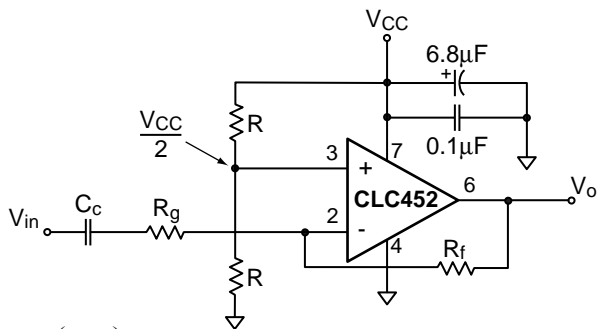
Figures 3 and 4 show possible non-inverting and inverting configurations for input signals that go below 0.8V DC. The input is AC coupled to prevent the need for level shifting the input signal at the source. The resistive voltage divider biases the non-inverting input to  $V_{CC} \div 2 = 2.5V$  (For  $V_{CC} = +5V$ ).



$$V_o = V_{in} \left( 1 + \frac{R_f}{R_g} \right) + 2.5$$

$$\text{low frequency cutoff} = \frac{1}{2\pi R_{in} C_c}, \text{ where: } R_{in} = \frac{R}{2} \quad R \gg R_{source}$$

Figure 3: AC Coupled Non-Inverting Configuration



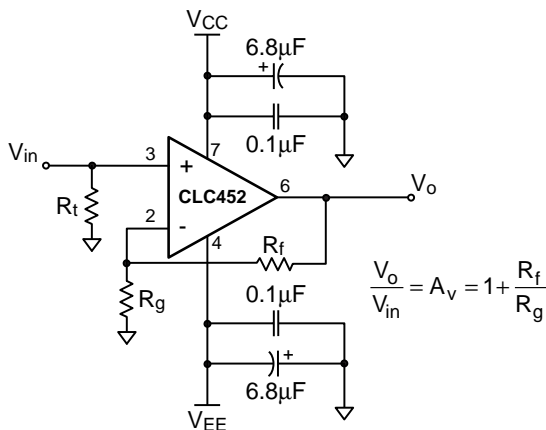
$$V_o = V_{in} \left( -\frac{R_f}{R_g} \right) + 2.5$$

$$\text{low frequency cutoff} = \frac{1}{2\pi R_g C_c}$$

Figure 4: AC Coupled Inverting Configuration

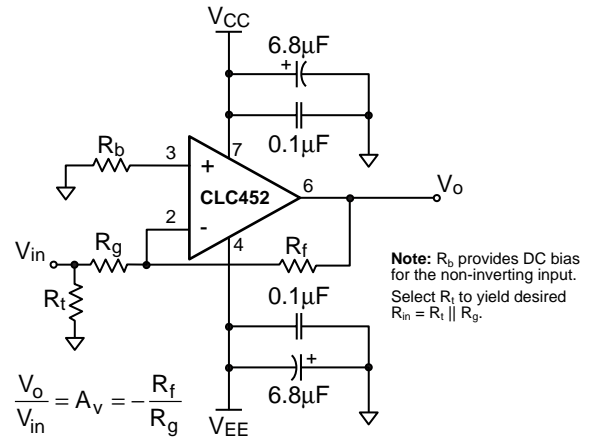
### Dual Supply Operation

The CLC452 operates on dual supplies as well as single supplies. The non-inverting and inverting configurations are shown in Figures 5 and 6.



$$\frac{V_o}{V_{in}} = A_v = 1 + \frac{R_f}{R_g}$$

Figure 5: Dual Supply Non-Inverting Configuration



Note:  $R_b$  provides DC bias for the non-inverting input. Select  $R_t$  to yield desired  $R_{in} = R_t \parallel R_g$ .

Figure 6: Dual Supply Inverting Configuration

### Feedback Resistor Selection

The feedback resistor,  $R_f$ , affects the loop gain and frequency response of a current feedback amplifier. Optimum performance of the CLC452, at a gain of  $+2V/V$ , is achieved with  $R_f$  equal to  $1k\Omega$ . The frequency response plots in the **Typical Performance** sections illustrate the recommended  $R_f$  for several gains. These recommended values of  $R_f$  provide the maximum bandwidth with minimal peaking. Within limits,  $R_f$  can be adjusted to optimize the frequency response.

- Decrease  $R_f$  to peak frequency response and extend bandwidth
- Increase  $R_f$  to roll off frequency response and compress bandwidth

As a rule of thumb, if the recommended  $R_f$  is doubled, then the bandwidth will be cut in half.

### Unity Gain Operation

The recommended  $R_f$  for unity gain ( $+1V/V$ ) operation is  $1k\Omega$ .  $R_g$  is left open. Parasitic capacitance at the inverting node may require a slight increase in  $R_f$  to maintain a flat frequency response.

### Bandwidth vs. Output Amplitude

The bandwidth of the CLC452 is at a maximum for output voltages near  $1V_{pp}$ . The bandwidth decreases for smaller and larger output amplitudes. Refer to the **Frequency Response vs.  $V_o$**  plots.

### Load Termination

The CLC452 can source and sink near equal amounts of current. For optimum performance, the load should be tied to  $V_{cm}$ .

### Driving Cables and Capacitive Loads

When driving cables, double termination is used to prevent reflections. For capacitive load applications, a small series resistor at the output of the CLC452 will improve stability and settling performance. The **Frequency Response vs.  $C_L$**  and **Recommended  $R_s$  vs.  $C_L$**  plots, in the typical performance section, give the recommended series resistance value for optimum flatness at various capacitive loads.



## Transmission Line Matching

One method for matching the characteristic impedance ( $Z_0$ ) of a transmission line or cable is to place the appropriate resistor at the input or output of the amplifier. Figure 7 shows typical inverting and non-inverting circuit configurations for matching transmission lines.

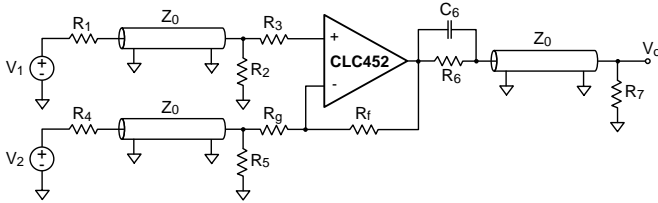


Figure 7: Transmission Line Matching

Non-inverting gain applications:

- Connect  $R_9$  directly to ground.
- Make  $R_1$ ,  $R_2$ ,  $R_6$ , and  $R_7$  equal to  $Z_0$ .
- Use  $R_3$  to isolate the amplifier from reactive loading caused by the transmission line, or by parasitics.

Inverting gain applications:

- Connect  $R_3$  directly to ground.
- Make the resistors  $R_4$ ,  $R_6$ , and  $R_7$  equal to  $Z_0$ .
- Make  $R_5 \parallel R_9 = Z_0$ .

The input and output matching resistors attenuate the signal by a factor of 2, therefore additional gain is needed. Use  $C_6$  to match the output transmission line over a greater frequency range.  $C_6$  compensates for the increase of the amplifier's output impedance with frequency.

## Power Dissipation

Follow these steps to determine the power consumption of the CLC452:

1. Calculate the quiescent (no-load) power:  

$$P_{amp} = I_{CC} (V_{CC} - V_{EE})$$
2. Calculate the RMS power at the output stage:  

$$P_o = (V_{CC} - V_{load}) (I_{load})$$
, where  $V_{load}$  and  $I_{load}$  are the RMS voltage and current across the external load.
3. Calculate the total RMS power:  

$$P_t = P_{amp} + P_o$$

The maximum power that the DIP, SOIC, and SOT packages can dissipate at a given temperature is illustrated in Figure 8. The power derating curve for any CLC452 package can be derived by utilizing the following equation:

$$\frac{(175^\circ - T_{amb})}{\theta_{JA}}$$

where

$T_{amb}$  = Ambient temperature ( $^\circ\text{C}$ )

$\theta_{JA}$  = Thermal resistance, from junction to ambient, for a given package ( $^\circ\text{C}/\text{W}$ )

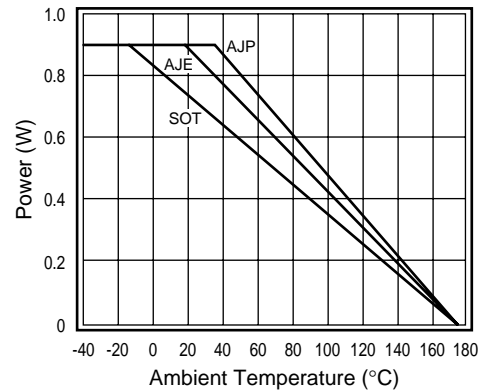


Figure 8: Power Derating Curves

## Layout Considerations

A proper printed circuit layout is essential for achieving high frequency performance. Comlinear provides evaluation boards for the CLC452 (730013-DIP, 730027-SOIC, 730068-SOT) and suggests their use as a guide for high frequency layout and as an aid for device testing and characterization.

General layout and supply bypassing play major roles in high frequency performance. Follow the steps below as a basis for high frequency layout:

- Include 6.8 $\mu\text{F}$  tantalum and 0.1 $\mu\text{F}$  ceramic capacitors on both supplies.
- Place the 6.8 $\mu\text{F}$  capacitors within 0.75 inches of the power pins.
- Place the 0.1 $\mu\text{F}$  capacitors less than 0.1 inches from the power pins.
- Remove the ground plane under and around the part, especially near the input and output pins to reduce parasitic capacitance.
- Minimize all trace lengths to reduce series inductances.
- Use flush-mount printed circuit board pins for prototyping, never use high profile DIP sockets.

## Evaluation Board Information

Data sheets are available for the CLC730013/CLC730027 and CLC730068 evaluation boards. The evaluation board data sheets provide:

- Evaluation board schematics
- Evaluation board layouts
- General information about the boards

The CLC730013/CLC730027 data sheet also contains tables of recommended components to evaluate several of Comlinear's high speed amplifiers. This table for the CLC452 is illustrated below. Refer to the evaluation board data sheet for schematics and further information.

## Components Needed to Evaluate the CLC452 on the Evaluation Board:

- $R_f$ ,  $R_g$  - Use this product data sheet to select values
- $R_{in}$ ,  $R_{out}$  - Typically 50 $\Omega$  (Refer to the **Basic Operation** section of the evaluation board data sheet for details)

- $R_f$  - Optional resistor for inverting gain configurations (Select  $R_f$  to yield desired input impedance =  $R_g \parallel R_f$ )
- $C_1, C_2$  - 0.1 $\mu$ F ceramic capacitors
- $C_3, C_4$  - 6.8 $\mu$ F tantalum capacitors

Components not used:

- $C_5, C_6, C_7, C_8$
- $R_1$  thru  $R_8$

The evaluation boards are designed to accommodate dual supplies. The boards can be modified to provide single supply operation. For best performance; 1) do not connect the unused supply, 2) ground the unused supply pin.

### SPICE Models

SPICE models provide a means to evaluate amplifier designs. Free SPICE models are available for Comlinear's monolithic amplifiers that:

- Support Berkeley SPICE 2G and its many derivatives
- Reproduce typical DC, AC, Transient, and Noise performance
- Support room temperature simulations

The *readme* file that accompanies the diskette lists released models, and provides a list of modeled parameters. The application note OA-18, Simulation SPICE Models for Comlinear's Op Amps, contains schematics and a reproduction of the readme file.

## Application Circuits

### Single Supply Cable Driver

The typical application shown on the front page shows the CLC452 driving 10m of 75 $\Omega$  coaxial cable. The CLC452 is set for a gain of +2V/V to compensate for the divide-by-two voltage drop at  $V_o$ .

### Single Supply Lowpass Filter

Figures 9 and 10 illustrate a lowpass filter and design equations. The circuit operates from a single supply of +5V. The voltage divider biases the non-inverting input to 2.5V. And the input is AC coupled to prevent the need for level shifting the input signal at the source. Use the design equations to determine  $R_1, R_2, C_1,$  and  $C_2$  based on the desired Q and corner frequency.

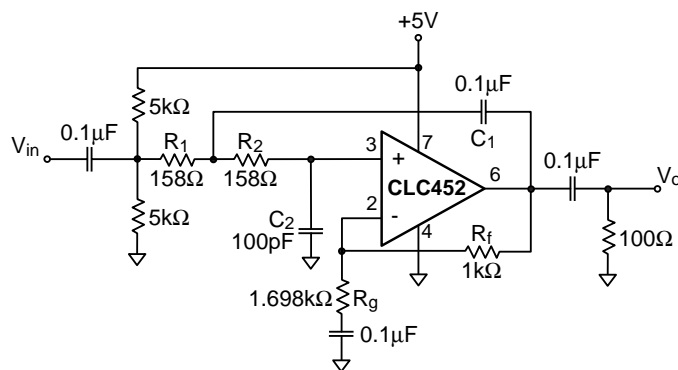


Figure 9: Lowpass Filter Topology

$$\text{Gain} = K = 1 + \frac{R_f}{R_g}$$

$$\text{Corner frequency} = \omega_c = \sqrt{\frac{1}{R_1 R_2 C_1 C_2}}$$

$$Q = \frac{1}{\sqrt{\frac{R_2 C_2}{R_1 C_1} + \frac{R_1 C_2}{R_2 C_1} + (1-K) \sqrt{\frac{R_1 C_1}{R_2 C_2}}}}$$

For  $R_1 = R_2 = R$  and  $C_1 = C_2 = C$

$$\omega_c = \frac{1}{RC}$$

$$Q = \frac{1}{(3-K)}$$

Figure 10: Design Equations

This example illustrates a lowpass filter with  $Q = 0.707$  and corner frequency  $f_c = 10\text{MHz}$ . A Q of 0.707 was chosen to achieve a maximally flat, Butterworth response. Figure 11 indicates the filter response.

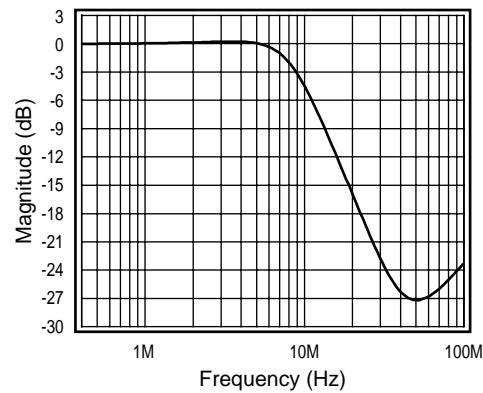


Figure 11: Lowpass Response

### Twisted Pair Driver

The high output current and low distortion, of the CLC452, make it well suited for driving transformers. Figure 12 illustrates a typical twisted pair driver utilizing the CLC452 and a transformer. The transformer provides the signal and its inversion for the twisted pair.

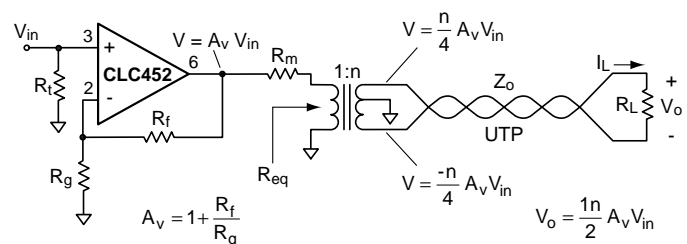


Figure 12: Twisted Pair Driver

To match the line's characteristic impedance ( $Z_o$ ) set:

- $R_L = Z_o$
- $R_m = R_{eq}$

Where  $R_{eq}$  is the transformed value of the load impedance, ( $R_L$ ), and is approximated by:

$$R_{eq} = \frac{R_L}{n^2}$$

Select the transformer so that it loads the line with a value close to  $Z_0$ , over the desired frequency range. The output impedance,  $R_o$ , of the CLC452 varies with frequency and can also affect the return loss. The return loss, shown below, takes into account an ideal transformer and the value of  $R_o$ .

$$\text{Return Loss (dB)} \approx -20 \log_{10} \left| n^2 \cdot \frac{R_o}{Z_0} \right|$$

The load current ( $I_L$ ) and voltage ( $V_o$ ) are related to the CLC452's maximum output voltage and current by:

$$|V_o| \leq n \cdot V_{max}$$

$$|I_L| \leq \frac{I_{max}}{n}$$

From the above current relationship, it is obvious that an amplifier with high output drive capability is required.

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