

Dual, 400MHz, Low Power, Video Operational Amplifier

The HFA1205 is a dual, high speed, low power current feedback amplifier built with Intersil's proprietary complementary bipolar UHF-1 process.

These amplifiers deliver 400MHz bandwidth and 1275V/ μ s slew rate, on only 60mW of quiescent power. They are specifically designed to meet the performance, power, and cost requirements of high volume video applications. The excellent gain flatness and differential gain/phase performance make these amplifiers well suited for component or composite video applications. Video performance is maintained even when driving a back terminated cable ($R_L = 150\Omega$), and degrades only slightly when driving two back terminated cables ($R_L = 75\Omega$). RGB applications will benefit from the high slew rates, and high full power bandwidth.

The HFA1205 is a pin compatible, low power, high performance upgrade for the popular Intersil HA5023. For a dual amplifier with output disable capability, please see the HFA1245 datasheet.

Ordering Information

PART NUMBER (BRAND)	TEMP. RANGE (°C)	PACKAGE	PKG. NO.
HFA1205IP	-40 to 85	8 Ld PDIP	E8.3
HFA1205IB (H1205I)	-40 to 85	8 Ld SOIC	M8.15
HA5023EVAL	High Speed Op Amp DIP Evaluation Board		

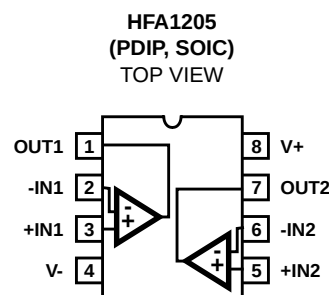
Features

- Low Supply Current 5.8mA/Op Amp
- High Input Impedance $2M\Omega$
- Wide -3dB Bandwidth ($A_V = +2$) 400MHz
- Very Fast Slew Rate 1275V/ μ s
- Gain Flatness (to 50MHz) $\pm 0.03\text{dB}$
- Differential Gain 0.03%
- Differential Phase 0.03 Degrees
- Pin Compatible Upgrade to HA5023

Applications

- Flash A/D Drivers
- High Resolution Monitors
- Video Switching and Routing
- Professional Video Processing
- Video Digitizing Boards/Systems
- Multimedia Systems
- RGB Preamps
- Medical Imaging
- Hand Held and Miniaturized RF Equipment
- Battery Powered Communications
- High Speed Oscilloscopes and Analyzers

Pinout



Electrical Specifications $V_{\text{SUPPLY}} = \pm 5\text{V}$, $A_V = +1$, $R_F = 560\Omega$, $R_L = 100\Omega$, Unless Otherwise Specified **(Continued)**

PARAMETER	TEST CONDITIONS	(NOTE 3) TEST LEVEL	TEMP. (°C)	MIN	TYP	MAX	UNITS
Inverting Input Bias Current Power Supply Sensitivity	$\Delta V_{\text{PS}} = \pm 1.8\text{V}$	A	25	-	2	5	$\mu\text{A/V}$
	$\Delta V_{\text{PS}} = \pm 1.8\text{V}$	A	85	-	4	8	$\mu\text{A/V}$
	$\Delta V_{\text{PS}} = \pm 1.2\text{V}$	A	-40	-	4	8	$\mu\text{A/V}$
Inverting Input Resistance		C	25	-	60	-	Ω
Input Capacitance		C	25	-	1.6	-	pF
Input Voltage Common Mode Range (Implied by V_{IO} CMRR, $+R_{\text{IN}}$, and $-I_{\text{BIAS}}$ CMS tests)		A	25, 85	± 1.8	± 2.4	-	V
		A	-40	± 1.2	± 1.7	-	V
Input Noise Voltage Density	$f = 100\text{kHz}$	B	25	-	3.5	-	$\text{nV}/\sqrt{\text{Hz}}$
Non-Inverting Input Noise Current Density	$f = 100\text{kHz}$	B	25	-	2.5	-	$\text{pA}/\sqrt{\text{Hz}}$
Inverting Input Noise Current Density	$f = 100\text{kHz}$	B	25	-	20	-	$\text{pA}/\sqrt{\text{Hz}}$
TRANSFER CHARACTERISTICS							
Open Loop Transimpedance Gain	$A_V = -1$	C	25	-	500	-	$\text{k}\Omega$
AC CHARACTERISTICS $A_V = +2$, $R_F = 464\Omega$, Unless Otherwise Specified							
-3dB Bandwidth ($V_{\text{OUT}} = 0.2V_{\text{P-P}}$)	$A_V = +1$, $R_S = 432\Omega$	B	25	-	280	-	MHz
	$A_V = +2$	B	25	-	400	-	MHz
	$A_V = -1$, $R_F = 332\Omega$	B	25	-	360	-	MHz
Full Power Bandwidth ($V_{\text{OUT}} = 5V_{\text{P-P}}$ at $A_V = +2/-1$, $4V_{\text{P-P}}$ at $A_V = +1$)	$A_V = +1$, $R_S = 432\Omega$	B	25	-	140	-	MHz
	$A_V = +2$	B	25	-	125	-	MHz
	$A_V = -1$, $R_F = 332\Omega$	B	25	-	180	-	MHz
Gain Flatness ($A_V = +2$, $V_{\text{OUT}} = 0.2V_{\text{P-P}}$)	To 25MHz	B	25	-	± 0.02	-	dB
	To 50MHz	B	25	-	± 0.03	-	dB
Minimum Stable Gain		A	Full	-	1	-	V/V
Crosstalk	5MHz	B	25	-	-60	-	dB
	10MHz	B	25	-	-54	-	dB
OUTPUT CHARACTERISTICS $R_F = 560\Omega$, Unless Otherwise Specified							
Output Voltage Swing	$A_V = -1$, $R_L = 100\Omega$	A	25	± 3	± 3.4	-	V
		A	Full	± 2.8	± 3	-	V
Output Current	$A_V = -1$, $R_L = 50\Omega$	A	25, 85	50	60	-	mA
		A	-40	28	42	-	mA
Output Short Circuit Current		B	25	-	90	-	mA
Closed Loop Output Impedance	DC, $A_V = +2$, $R_F = 464\Omega$	B	25	-	0.07	-	Ω
Second Harmonic Distortion ($A_V = +2$, $R_F = 464\Omega$, $V_{\text{OUT}} = 2V_{\text{P-P}}$)	10MHz	B	25	-	-50	-	dBc
	20MHz	B	25	-	-45	-	dBc
Third Harmonic Distortion ($A_V = +2$, $R_F = 464\Omega$, $V_{\text{OUT}} = 2V_{\text{P-P}}$)	10MHz	B	25	-	-55	-	dBc
	20MHz	B	25	-	-50	-	dBc
TRANSIENT CHARACTERISTICS $A_V = +2$, $R_F = 464\Omega$, Unless Otherwise Specified							
Rise and Fall Times ($V_{\text{OUT}} = 0.5V_{\text{P-P}}$)	Rise Time	B	25	-	0.8	-	ns
	Fall Time	B	25	-	1.25	-	ns

Electrical Specifications $V_{\text{SUPPLY}} = \pm 5\text{V}$, $A_V = +1$, $R_F = 560\Omega$, $R_L = 100\Omega$, Unless Otherwise Specified **(Continued)**

PARAMETER	TEST CONDITIONS	(NOTE 3) TEST LEVEL	TEMP. (°C)	MIN	TYP	MAX	UNITS
Overshoot	$V_{\text{OUT}} = 0.5V_{\text{P-P}}$, $V_{\text{IN}} t_{\text{RISE}} = 2.5\text{ns}$	B	25	-	5	-	%
Slew Rate ($V_{\text{OUT}} = 4V_{\text{P-P}}$, $A_V = +1$, $R_S = 432\Omega$)	+SR	B	25	-	1050	-	V/ μs
	-SR	B	25	-	750	-	V/ μs
Slew Rate ($V_{\text{OUT}} = 5V_{\text{P-P}}$, $A_V = +2$)	+SR	B	25	-	1375	-	V/ μs
	-SR	B	25	-	875	-	V/ μs
Slew Rate ($V_{\text{OUT}} = 5V_{\text{P-P}}$, $A_V = -1$, $R_F = 332\Omega$)	+SR	B	25	-	2250	-	V/ μs
	-SR	B	25	-	1275	-	V/ μs
Settling Time ($V_{\text{OUT}} = +2\text{V}$ to 0V step)	To 0.1%	B	25	-	15	-	ns
	To 0.05%	B	25	-	20	-	ns
	To 0.02%	B	25	-	30	-	ns
Overdrive Recovery Time	$V_{\text{IN}} = \pm 2\text{V}$	B	25	-	10	-	ns
VIDEO CHARACTERISTICS $A_V = +2$, $R_F = 464\Omega$, Unless Otherwise Specified							
Differential Gain ($f = 3.58\text{MHz}$)	$R_L = 150\Omega$	B	25	-	0.03	-	%
	$R_L = 75\Omega$	B	25	-	0.03	-	%
Differential Phase ($f = 3.58\text{MHz}$)	$R_L = 150\Omega$	B	25	-	0.03	-	Degrees
	$R_L = 75\Omega$	B	25	-	0.05	-	Degrees
POWER SUPPLY CHARACTERISTICS							
Power Supply Range		C	25	± 4.5	-	± 5.5	V
Power Supply Current		A	25	5.6	5.8	6.1	mA/ Op Amp
		A	Full	5.4	5.9	6.3	mA/ Op Amp

NOTE:

3. Test Level: A. Production Tested.; B. Typical or Guaranteed Limit Based on Characterization.; C. Design Typical for Information Only.

Application Information**Optimum Feedback Resistor**

Although a current feedback amplifier's bandwidth dependency on closed loop gain isn't as severe as that of a voltage feedback amplifier, there can be an appreciable decrease in bandwidth at higher gains. This decrease may be minimized by taking advantage of the current feedback amplifier's unique relationship between bandwidth and R_F . All current feedback amplifiers require a feedback resistor, even for unity gain applications, and R_F , in conjunction with the internal compensation capacitor, sets the dominant pole of the frequency response. Thus, the amplifier's bandwidth is inversely proportional to R_F . The HFA1205 design is optimized for a 464Ω R_F at a gain of +2. Decreasing R_F decreases stability, resulting in excessive peaking and overshoot (Note: Capacitive feedback will cause the same problems due to the feedback impedance decrease at higher frequencies). At

higher gains the amplifier is more stable, so R_F can be decreased in a trade-off of stability for bandwidth.

The table below lists recommended R_F values for various gains, and the expected bandwidth. For good channel-to-channel gain matching, it is recommended that all resistors (termination as well as gain setting) be $\pm 1\%$ tolerance or better. Note that a series input resistor, on +IN, is required for a gain of +1, to reduce gain peaking and increase stability.

GAIN (A_{CL})	R_F (Ω)	BANDWIDTH (MHz)
-1	332	360
+1	464 ($+R_S = 432\Omega$)	280
+2	464	400

Non-inverting Input Source Impedance

For best operation, the DC source impedance seen by the non-inverting input should be $\geq 50\Omega$. This is especially important in inverting gain configurations where the non-inverting input would normally be connected directly to GND.

PC Board Layout

The frequency response of this amplifier depends greatly on the amount of care taken in designing the PC board. **The use of low inductance components such as chip resistors and chip capacitors is strongly recommended, while a solid ground plane is a must!**

Attention should be given to decoupling the power supplies. A large value ($10\mu\text{F}$) tantalum in parallel with a small value ($0.1\mu\text{F}$) chip capacitor works well in most cases.

Terminated microstrip signal lines are recommended at the input and output of the device. Capacitance directly on the output must be minimized, or isolated as discussed in the next section.

Care must also be taken to minimize the capacitance to ground seen by the amplifier's inverting input (-IN). The larger this capacitance, the worse the gain peaking, resulting in pulse overshoot and possible instability. To this end, it is recommended that the ground plane be removed under traces connected to -IN, and connections to -IN should be kept as short as possible.

Driving Capacitive Loads

Capacitive loads, such as an A/D input, or an improperly terminated transmission line will degrade the amplifier's phase margin resulting in frequency response peaking and possible oscillations. In most cases, the oscillation can be avoided by placing a resistor (R_S) in series with the output prior to the capacitance.

Figure 1 details starting points for the selection of this resistor. The points on the curve indicate the R_S and C_L combinations for the optimum bandwidth, stability, and settling time, but experimental fine tuning is recommended. Picking a point above or to the right of the curve yields an overdamped response, while points below or left of the curve indicate areas of underdamped performance.

R_S and C_L form a low pass network at the output, thus limiting system bandwidth well below the amplifier bandwidth of 280MHz (for $A_V = +1$). By decreasing R_S as C_L increases (as illustrated in the curves), the maximum bandwidth is obtained without sacrificing stability. In spite of this, bandwidth decreases as the load capacitance increases. For example, at $A_V = +1$, $R_S = 62\Omega$, $C_L = 40\text{pF}$, the overall bandwidth is limited to 180MHz, and bandwidth drops to 70MHz at $A_V = +1$, $R_S = 8\Omega$, $C_L = 400\text{pF}$.

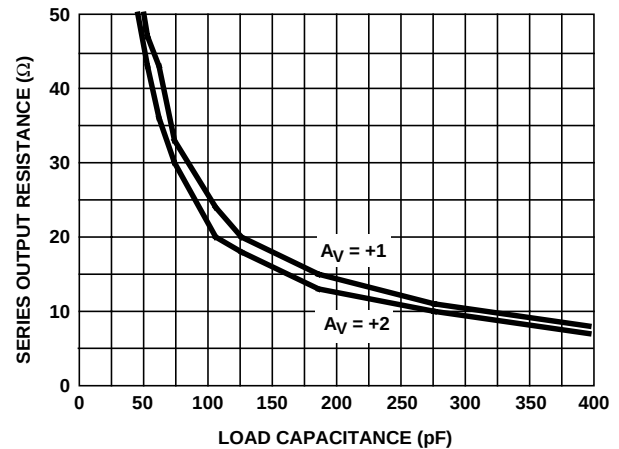


FIGURE 1. RECOMMENDED SERIES OUTPUT RESISTOR vs LOAD CAPACITANCE

Evaluation Board

The performance of the HFA1205 may be evaluated using the HA5023 Evaluation Board. The feedback and gain setting resistors must be replaced with the appropriate value (see "Optimum Feedback Resistor" section) for the gain being evaluated. Also, replace the two 0Ω series output resistors with 50Ω resistors.

To order evaluation boards (Part Number HA5023EVAL), please contact your local sales office.

Typical Performance Curves $V_{\text{SUPPLY}} = \pm 5\text{V}$, $R_F = \text{Optimum Value From "Apps Info" Table}$, $T_A = 25^\circ\text{C}$, $R_L = 100\Omega$, Unless Otherwise Specified

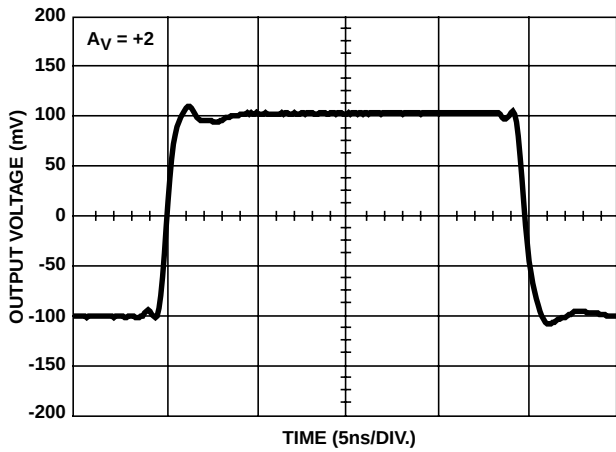


FIGURE 2. SMALL SIGNAL PULSE RESPONSE

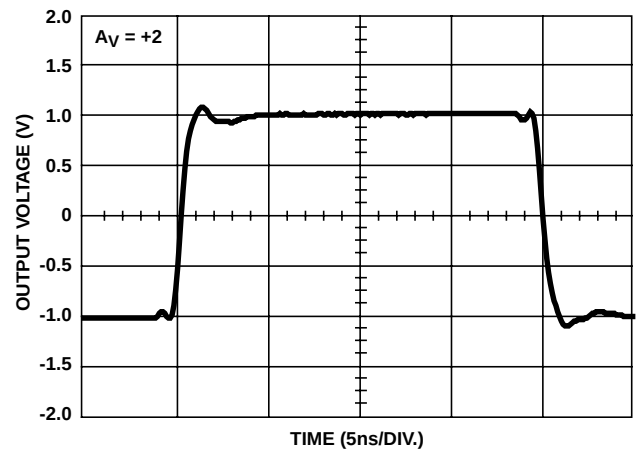


FIGURE 3. LARGE SIGNAL PULSE RESPONSE

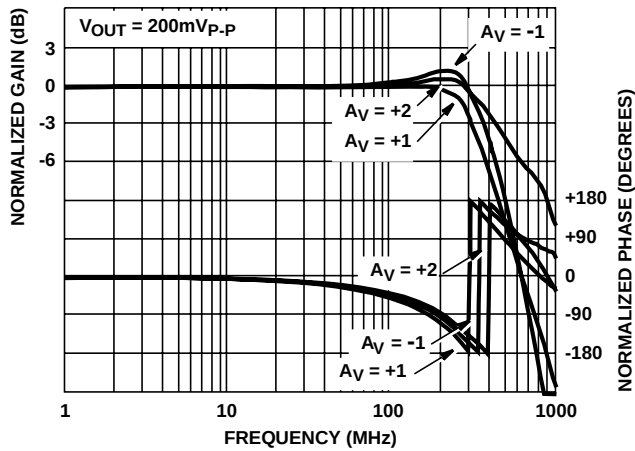


FIGURE 4. FREQUENCY RESPONSE

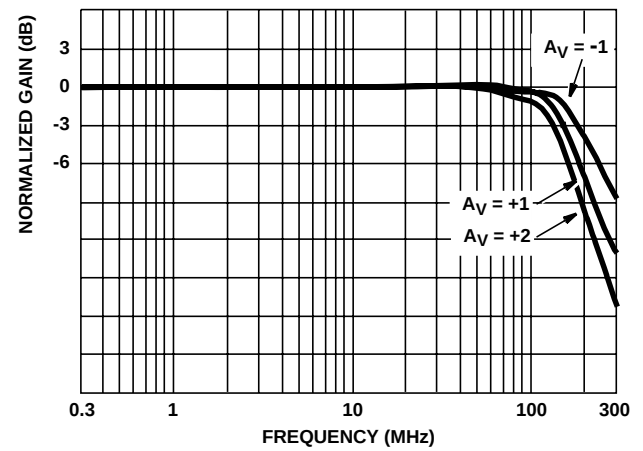


FIGURE 5. FULL POWER BANDWIDTH

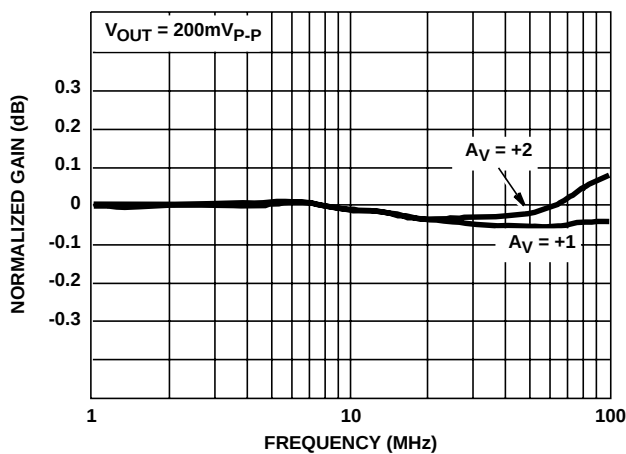


FIGURE 6. GAIN FLATNESS

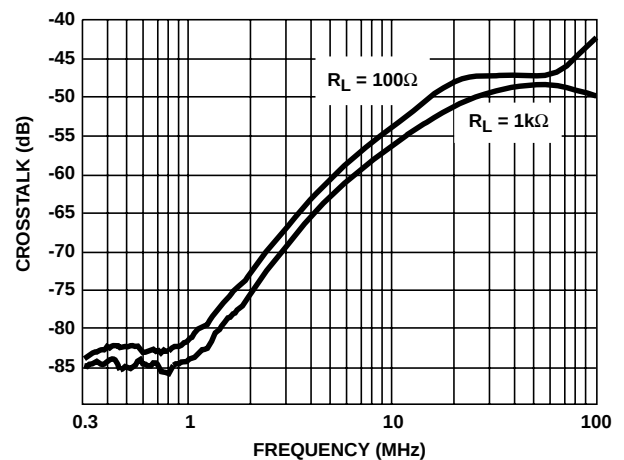


FIGURE 7. CROSSTALK vs FREQUENCY

Die Characteristics

DIE DIMENSIONS:

69 mils x 92 mils x 19 mils
 1750 μ m x 2330 μ m x 483 μ m

METALLIZATION:

Type: Metal 1: AlCu(2%)/TiW
 Thickness: Metal 1: 8k $\text{\AA}$ $\pm$ 0.4k $\text{\AA}$
 Type: Metal 2: AlCu(2%)
 Thickness: Metal 2: 16k $\text{\AA}$ $\pm$ 0.8k $\text{\AA}$

SUBSTRATE POTENTIAL (Powered Up):

Floating (Recommend Connection to V-)

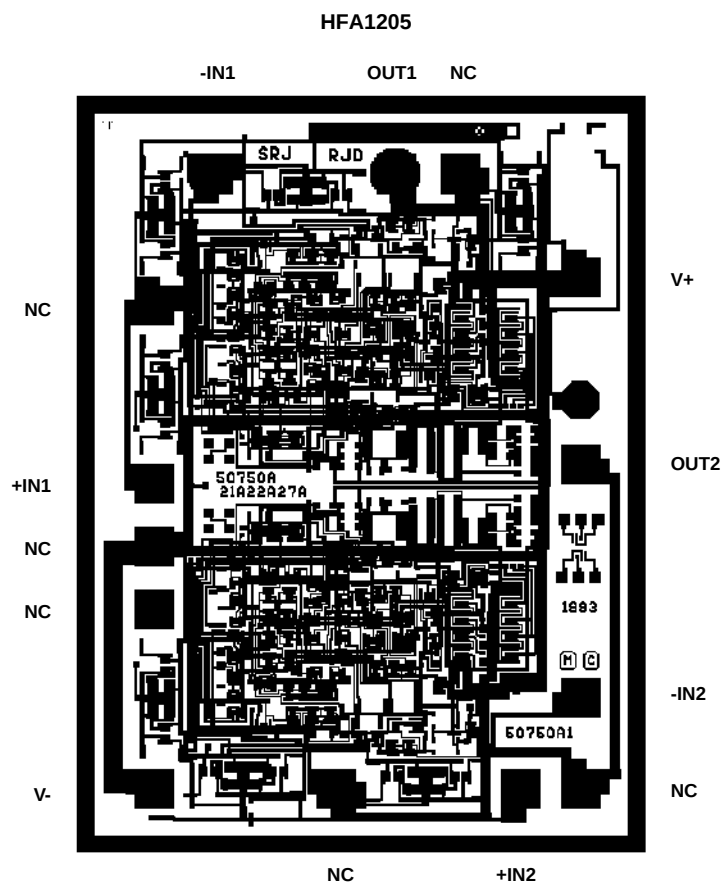
PASSIVATION:

Type: Nitride
 Thickness: 4k $\text{\AA}$ $\pm$ 0.5k $\text{\AA}$

TRANSISTOR COUNT:

180

Metallization Mask Layout



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